16-Bit, 200 MSPS/500 MSPS TxDAC+® with 2×/4×/8× Interpolation and Signal Processing

AD9786

FEATURES

16-bit resolution, 200 MSPS input data rate
IMD 90 dBc @10 MHz
Noise spectral density (NSD) −164 dBm/Hz @ 10 MHz
WCDMA ACLR = 80 dBc @ 40 MHz IF
DNL = ±0.3 LSB
INL = ±0.6 LSB
Selectable 2×/4×/8× interpolation filters
Selectable $f_{DAC}/2$, $f_{DAC}/4$, $f_{DAC}/8$ modulation modes
Single or dual channel signal processing
Selectable image rejection Hilbert transform
Flexible calibration engine
Direct IF transmission features
Serial control interface
Versatile clock and data interface
3.3 V compatible digital interface
On-chip 1.2 V reference
80-lead thermally enhanced TQFP package

APPLICATIONS

Base stations: Multicarrier WCDMA, GSM/EDGE, TD-SCDMA, IS136, TETRA
Instrumentation: RF Signal Generators, Arbitrary Waveform Generators
HDTV Transmitters
Broadband Wireless Systems
Digital Radio Links
Satellite Systems

PRODUCT DESCRIPTION

The AD9786 is a 16-bit, high speed, CMOS DAC with 2×/4×/8× interpolation and signal processing features tuned for communications applications. It offers state-of-the-art distortion and noise performance. The AD9786 was developed to meet the demanding performance requirements of multicarrier and third generation base stations. The selectable interpolation filters simplify interfacing to a variety of input data rates while also taking advantage of oversampling performance gains. The modulation modes allow convenient bandwidth placement and selectable sideband suppression.

The flexible clock interface accepts a variety of input types such as 1 V p-p sine wave, CMOS, and LVPECL in single-ended or differential mode. Internal dividers generate the required data rate interface clocks.

The AD9786 provides a differential current output, supporting single-ended or differential applications; it provides a nominal full-scale current from 10 mA to 20 mA. The AD9786 is manufactured on an advanced low cost 0.25 μm CMOS process.

FUNCTIONAL BLOCK DIAGRAM

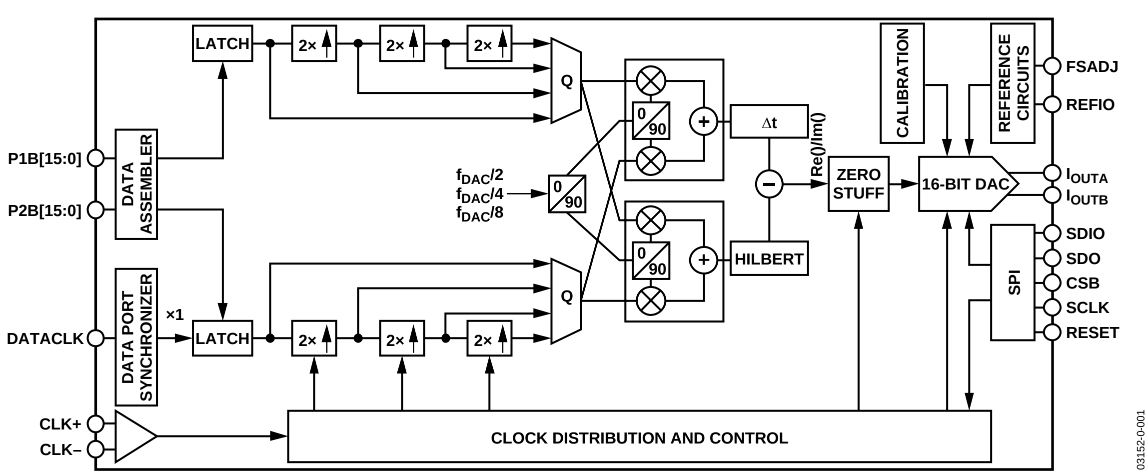

Figure 1.

Rev. 0

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REVISION HISTORY

7/04—Revision 0: Initial Version

PRODUCT HIGHLIGHTS

1. The AD9786 is a 16-bit high speed interpolating TxDAC+.
2. 2×/4×/8× user selectable interpolating filter eases data rate and output signal reconstruction filter requirements.
3. 200 MSPS input data rate.
4. Ultra high speed 500 MSPS DAC conversion rate.
5. Flexible clock with single-ended or differential input: CMOS, 1 V p-p sine wave, and LVPECL capability.
6. Complete CMOS DAC function operates from a 3.1 V to 3.5 V single analog (AVDD) supply, 2.5 V (DVDD) digital supply, and a 2.5 to 3.3V DRVDD supply. The DAC full-scale current can be reduced for lower power operation, and a sleep mode is provided for low power idle periods.
7. On-chip voltage reference: The AD9786 includes a 1.20 V temperature-compensated band gap voltage reference.
8. Multichip synchronization: Multiple AD9786 DACs can be synchronized to a single master AD9786 to ease timing design requirements and optimize image reject transmit performance.

SPECIFICATIONS

DC SPECIFICATIONS

T_{MIN} to T_{MAX}, AVDD1, AVDD2 = 3.3 V, ACVDD, ADVDD, CLKVDD, DVDD, DRVDD = 2.5 V, I_{OUTFS} = 20 mA, unless otherwise noted.

Table 1.

Parameter	Min	Typ	Max	Unit
RESOLUTION		16		Bits
DC Accuracy[1]				
Integral Nonlinearity		±0.6		LSB
Differential Nonlinearity		±0.3		LSB
ANALOG OUTPUT				
Offset Error		±0.015	±0.0175	% of FSR
Gain Error (with Internal Reference)		±1.5		% of FSR
Full-Scale Output Current[2]	10		20	mA
Output Compliance Range	−1.0		+1.0	V
Output Resistance		10		MΩ
REFERENCE OUTPUT				
Reference Voltage	1.15	1.23	1.30	V
Reference Output Current[3]		1		µA
REFERENCE INPUT				
Input Compliance Range	0.1		1.25	V
Reference Input Resistance (Ext Reference Mode)		10		MΩ
Small Signal Bandwith		200		kHz
TEMPERATURE COEFFICIENTS				
Unipolar Offset Drift		0		ppm of FSR/°C
Gain Drift (with Internal Reference)		±4		ppm of FSR/°C
Reference Voltage Drift		±30		ppm/°C
POWER SUPPLY				
AVDD1, AVDD2				
Voltage Range	3.1	3.3	3.5	V
Analog Supply Current ($I_{AVDD1} + I_{AVDD2}$)		50		mA
$I_{AVDD1} + I_{AVDD2}$ in SLEEP Mode		18		mA
ACVDD, ADVDD				
Voltage Range	2.35	2.5	2.65	V
Analog Supply Current ($I_{ACVDD} + I_{ADVDD}$)		2.5		mA
CLKVDD				
Voltage Range	2.35	2.5	2.65	V
Clock Supply Current (I_{CLKVDD})		12		mA
DVDD				
Voltage Range	2.35	2.5	2.65	V
Digital Supply Current (I_{DVDD})		52.5		mA
DRVDD				
Voltage Range	2.35	2.5/3.3	3.5	V
Digital Supply Current (I_{DRVDD})		5.3		µA
Nominal Power Dissipation[4]		1.25		W
OPERATING RANGE	−40		+85	°C

[1] Measured at IOUTA driving a virtual ground.
[2] Nominal full-scale current, I_{OUTFS}, is 32× the I_{REF} current.
[3] Use an external amplifier to drive any external load.
[4] Measured under the following conditions: f_{DATA} = 125 MSPS, f_{DAC} = 500 MSPS, 4× interpolation, f_{DAC}/4 modulation, Hilbert Off.

DYNAMIC SPECIFICATIONS

T_{MIN} to T_{MAX}, AVDD1, AVDD2 = 3.3 V, ACVDD, ADVDD, CLKVDD, DVDD, DRVDD = 2.5 V, I_{OUTFS} = 20 mA, differential transformer coupled output, 50 Ω doubly terminated, unless otherwise noted.

Table 2.

Parameter	Min	Typ	Max	Unit
DYNAMIC PERFORMANCE				
Maximum DAC Output Update Rate (f_{DAC})	500			MSPS
Output Settling Time (t_{ST}) (to 0.025%)				ns
Output Propagation Delay[1] (t_{PD})				ns
Output Rise Time (10% to 90% of Full Scale)[2]				ns
Output Fall Time (90% to 10% of Full Scale)[2]				ns
AC LINEARITY-BASEBAND MODE				
Spurious-Free Dynamic Range (SFDR) to Nyquist (f_{OUT} = 0 dBFS)				
f_{DATA} = 100 MSPS; f_{OUT} = 5 MHz, 4×, 2× interpolation		93		dBc
f_{DATA} = 200 MSPS; f_{OUT} = 10 MHz		85		dBc
f_{DATA} = 200 MSPS; f_{OUT} = 25 MHz		78		dBc
f_{DATA} = 200 MSPS; f_{OUT} = 50 MHz		78		dBc
Two-Tone Intermodulation (IMD) to Nyquist (f_{OUT1} = f_{OUT2} = −6 dBFS)				
f_{DATA} = 200 MSPS; f_{OUT1} = 5 MHz; f_{OUT2} = 6 MHz		85		dBc
f_{DATA} = 200 MSPS; f_{OUT1} = 15 MHz; f_{OUT2} = 16 MHz		85		dBc
f_{DATA} = 200 MSPS; f_{OUT1} = 25 MHz; f_{OUT2} = 26 MHz		84		dBc
f_{DATA} = 200 MSPS; f_{OUT1} = 45 MHz; f_{OUT2} = 46 MHz		80		dBc
f_{DATA} = 200 MSPS; f_{OUT1} = 65 MHz; f_{OUT2} = 66 MHz		78		dBc
f_{DATA} = 200 MSPS; f_{OUT1} = 85 MHz; f_{OUT2} = 86 MHz		75		dBc
Noise Power Spectral Density (NPSD)				
f_{DATA} = 156 MSPS; f_{OUT} = 10 MHz; 0 dBFS, 8 tones, separation = 500 kHz		−164		dBm/Hz
f_{DATA} = 156 MSPS; f_{OUT} = 50 MHz; 0 dBFS, 8 tones, separation = 500 kHz		−161		dBm/Hz
Adjacent Channel Power Ratio (ACLR)				
WCDMA ACLR with 3.84 MHz BW, single carrier				
IF = 21 MHz, f_{DATA} = 122.88 MSPS, 4× interpolation		80		dB
IF = 224.76 MHz, f_{DATA} = 122.88 MSPS, 4× interpolation, high-pass interpolation filter mode		72		dB

[1] Propagation delay is delay from CLK input to DAC update.
[2] Measured doubly terminated into 50 Ω load.

DIGITAL SPECIFICATIONS

T_{MIN} to T_{MAX}, AVDD1, AVDD2 = 3.3 V, ACVDD, ADVDD, CLKVDD, DVDD = 2.5 V, I_{OUTFS} = 20 mA, unless otherwise noted.

Table 3.

Parameter	Min	Typ	Max	Unit
DIGITAL INPUTS				
Logic 1 Voltage	DRVDD – 0.9	DRVDD		V
Logic 0 Voltage		0	0.9	V
Logic 1 Current	–10		+10	µA
Logic 0 Current	–10		+10	µA
Input Capacitance		5		pF
CLOCK INPUTS				
Input Voltage Range	0		2.65	V
Common-Mode Voltage	0.75	1.5	2.25	V
Differential Voltage	0.5	1.5		V
Input Setup Time (t_S)[1]				
Input Hold Time (t_H)[1]				
Latch Pulse Width (t_{LPW})[1]				
CLK to PLLLOCK Delay (t_{OD})[1]				

[1]See timing specifications on Pages 26 to 31 for details in each timing mode.

ABSOLUTE MAXIMUM RATINGS

Table 4.

Parameter	With Respect to	Min	Max	Unit
AVDD1, AVDD2, DRVDD	AGND1, AGND2, ACGND, ADGND, CLKGND, DGND	−0.3	+3.6	V
ACVDD, ADVDD, CLKGND, DVDD	AGND1, AGND2, ACGND, ADGND, CLKGND, DGND	−0.3	+2.8	V
AGND1, AGND2, ACGND, ADGND, CLKGND, DGND	AGND1, AGND2, ACGND, ADGND, CLKGND, DGND	−0.3	+0.3	V
REFIO, FSADJ	AGND1	−0.3	AVDD1 + 0.3	V
I_{OUTA}, I_{OUTB}	AGND1	−1.0	AVDD1 + 0.3	V
P1B15-P1B0, P2B15-P2B0	DGND	−0.3	DVDD + 0.3	V
DATACLK	DGND	−0.3	DRVDD + 0.3	V
CLK+, CLK−, RESET	CLKGND	−0.3	CLKVDD + 0.3	V
CSB, SCLK, SDIO, SDO	DGND	−0.3	DVDD + 0.3	V
Junction Temperature		−65	+125	°C
Storage Temperature			150	°C
Lead temperature (10 sec)			300	°C

Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. This is a stress rating only; functional operation of the device at these or any other conditions above those indicated in the operational sections of this specification is not implied. Exposure to absolute maximum ratings for extended periods may affect device reliability.

THERMAL CHARACTERISTICS

Thermal Resistance

80-Lead Thermally Enhanced

TQFP Package θ_{JA} = 23.5° C/W (with thermal pad soldered to PCB)

ESD CAUTION

ESD (electrostatic discharge) sensitive device. Electrostatic charges as high as 4000 V readily accumulate on the human body and test equipment and can discharge without detection. Although this product features proprietary ESD protection circuitry, permanent damage may occur on devices subjected to high energy electrostatic discharges. Therefore, proper ESD precautions are recommended to avoid performance degradation or loss of functionality.

PIN CONFIGURATION AND FUNCTION DESCRIPTIONS

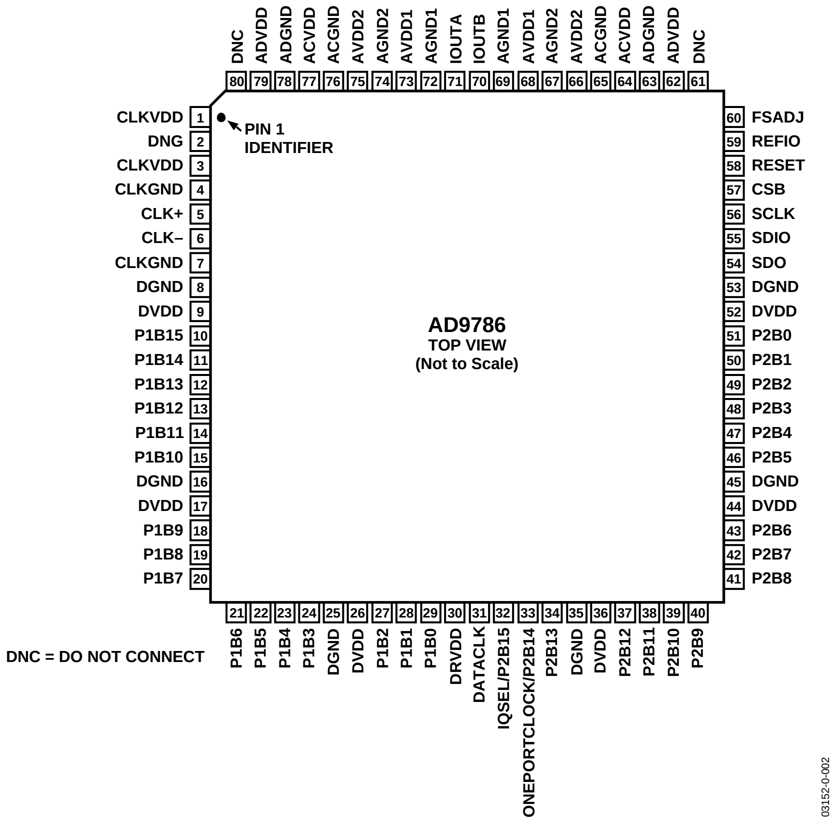


Figure 2. Pin Configuration

CLOCK

Table 5. Clock Pin Function Descriptions

Pin No.	Name	Direction	Description	
5, 6	CLK+, CLK–	I	Differential Clock Input.	
2	DNC		Do Not Connect.	
31	DATACLK	I/O	**DCLKEXT 02h[3]**	**Mode**
			0	Pin configured for input of channel data rate or synchronizer clock. Internal clock synchronizer may be turned on or off with DCLKCRC (02h[2]).
			1	Pin configured for output of channel data rate or synchronizer clock.
1, 3	CLKVDD		Clock Domain 2.5 V.	
4, 7	CLKGND		Clock Domain 0 V.	

ANALOG

Table 6. Analog Pin Function Descriptions

Pin No.	Name	Direction	Description
59	REFIO	A	Reference.
60	FSADJ	A	Full-Scale Adjust.
70, 71	IOUTB, IOUTA	A	Differential DAC Output Currents.
61	DNC		Do Not Connect.
62, 79	ADVDD		Analog Domain Digital Content 2.5 V.
63, 78	ADGND		Analog Domain Digital Content 0 V.
64, 77	ACVDD		Analog Domain Clock Content 2.5 V.
65, 76	ACGND		Analog Domain Clock Content 0 V.
66, 75	AVDD2		Analog Domain Clock Switching 3.3 V.
67, 74	AGND2		Analog Domain Switching 0 V.
68, 73	AVDD1		Analog Domain Quiet 3.3 V.
69, 72	AGND1		Analog Domain Quiet 0 V.
80	DNC		Do Not Connect.

DATA

Table 7. Data Pin Function Descriptions

<table>
<tr><th>Pin No.</th><th>Name</th><th>Direction</th><th>Description</th></tr>
<tr><td>10–15, 18–24, 27–29</td><td>P1B15–P1B0</td><td>I</td><td>Input Data Port One.
<table>
<tr><th>ONEPORT 02h[6]</th><th>Mode</th></tr>
<tr><td>0</td><td>Latched data routed for I channel processing.</td></tr>
<tr><td>1</td><td>Latched data demultiplexed by IQSEL and routed for interleaved I/Q processing.</td></tr>
</table></td></tr>
<tr><td>32</td><td>IQSEL/P2B15</td><td>I</td><td>
<table>
<tr><th>ONEPORT 02h[6]</th><th>IQPOL 02h[1]</th><th>IQSEL/ P2B15</th><th>Mode (IQPOL = 0)</th></tr>
<tr><td>0</td><td>X</td><td>X</td><td>Latched data routed to Q channel Bit 15 (MSB) processing.</td></tr>
<tr><td>1</td><td>0</td><td>0</td><td>Latched data on Data Port One routed to Q channel processing.</td></tr>
<tr><td>1</td><td>0</td><td>1</td><td>Latched data on Data Port One routed to I channel processing.</td></tr>
<tr><td>1</td><td>1</td><td>0</td><td>Latched data on Data Port One routed to I channel processing.</td></tr>
<tr><td>1</td><td>1</td><td>1</td><td>Latched data on Data Port One routed to Q channel processing.</td></tr>
</table></td></tr>
<tr><td>33</td><td>ONEPORTCLK/P2B14</td><td>I/O</td><td>
<table>
<tr><th>ONEPORT 02h[6]</th><th></th></tr>
<tr><td>0</td><td>Latched data routed for Q channel Bit 14 processing.</td></tr>
<tr><td>1</td><td>Pin configured for output of clock at twice the channel data route.</td></tr>
</table></td></tr>
<tr><td>34, 37-43, 46–51</td><td>P2B13-P2B0</td><td>I</td><td>Input Data Port Two Bits 13–0.</td></tr>
<tr><td>30</td><td>DRVDD</td><td></td><td>Digital Output Pin Supply, 2.5 V or 3.3 V.</td></tr>
<tr><td>9, 17, 26, 36, 44, 52</td><td>DVDD</td><td></td><td>Digital Domain 2.5 V.</td></tr>
<tr><td>8, 16, 25, 35, 45, 53</td><td>DGND</td><td></td><td>Digital Domain 0 V.</td></tr>
</table>

SERIAL INTERFACE

Table 8. Serial Interface Pin Function Descriptions

Pin No.	Name	Direction	Description		
54	SDO	O	**CSB**	**SDIODIR 00h[7]**	**Mode**
			1	X	High Impedance.
			0	0	Serial Data Output.
			0	1	High Impedance.
55	SDIO	I/O	**CSB**	**SDIODIR 00h[7]**	**Mode**
			1	X	High Impedance.
			0	0	Serial Data Output.
			0	1	Serial Data Input/Output Depending on Bit 7 of the Serial Instruction Byte.
56	SCLK	I	Serial Interface Clock.		
57	CSB	I	Serial Interface Chip Select.		
58	RESET	I	Resets entire chip to default state.		

DEFINITION OF SPECIFICATIONS

Linearity Error (Integral Nonlinearity or INL)

Linearity error is defined as the maximum deviation of the actual analog output from the ideal output, determined by a straight line drawn from zero to full scale.

Differential Nonlinearity (or DNL)

DNL is the measure of the variation in analog value, normalized to full scale, associated with a 1 LSB change in digital input code.

Monotonicity

A D/A converter is monotonic if the output either increases or remains constant as the digital input increases.

Offset Error

The deviation of the output current from the ideal of zero is called offset error. For I_{OUTA}, 0 mA output is expected when the inputs are all 0s. For I_{OUTB}, 0 mA output is expected when all inputs are set to 1s.

Gain Error

The difference between the actual and ideal output span. The actual span is determined by the output when all inputs are set to 1s, minus the output when all inputs are set to 0s.

Output Compliance Range

The range of allowable voltage at the output of a current-output DAC. Operation beyond the maximum compliance limits may cause either output stage saturation or breakdown, resulting in nonlinear performance.

Temperature Drift

Temperature drift is specified as the maximum change from the ambient (+25°C) value to the value at either T_{MIN} or T_{MAX}. For offset and gain drift, the drift is reported in ppm of full-scale range (FSR) per degree C. For reference drift, the drift is reported in ppm per degree C.

Power Supply Rejection

The maximum change in the full-scale output as the supplies are varied from minimum to maximum specified voltages.

Settling Time

The time required for the output to reach and remain within a specified error band about its final value, measured from the start of the output transition.

Glitch Impulse

Asymmetrical switching times in a DAC give rise to undesired output transients that are quantified by a glitch impulse. It is specified as the net area of the glitch in pV-s.

Spurious-Free Dynamic Range

The difference, in dB, between the rms amplitude of the output signal and the peak spurious signal over the specified bandwidth.

Total Harmonic Distortion

THD is the ratio of the rms sum of the first six harmonic components to the rms value of the measured fundamental. It is expressed as a percentage or in decibels (dB).

Signal-to-Noise Ratio (SNR)

S/N is the ratio of the rms value of the measured output signal to the rms sum of all other spectral components below the Nyquist frequency, excluding the first six harmonics and dc. The value for SNR is expressed in decibels.

Interpolation Filter

If the digital inputs to the DAC are sampled at a multiple rate of f_{DATA} (interpolation rate), a digital filter can be constructed which has a sharp transition band near $f_{DATA}/2$. Images that would typically appear around f_{DAC} (output data rate) can be greatly suppressed.

Pass Band

Frequency band in which any input applied therein passes unattenuated to the DAC output.

Stop-Band Rejection

The amount of attenuation of a frequency outside the pass band applied to the DAC, relative to a full-scale signal applied at the DAC input within the pass band.

Group Delay

Number of input clocks between an impulse applied at the device input and peak DAC output current. A half-band FIR filter has constant group delay over its entire frequency range

Impulse Response

Response of the device to an impulse applied to the input.

Adjacent Channel Leakage Ratio (or ACLR)

A ratio in dBc between the measured power within a channel relative to its adjacent channel.

Complex Modulation

The process of passing the real and imaginary components of a signal through a complex modulator (transfer function = e^{jwt} = coswt + jsinwt) and realizing real and imaginary components on the modulator output.

Hilbert Transform

A function with unity gain over all frequencies, but with a phase shift of 90 degrees for negative frequencies, and a phase shift of –90 degrees for positive frequencies. Although this function can not be implemented ideally, it can be approximated with a short FIR filter with enough accuracy to be very useful in single sideband radio architectures.

Complex Image Rejection

In a traditional two part upconversion, two images are created around the second IF frequency. These images are redundant and have the effect of wasting transmitter power and system bandwidth. By placing the real part of a second complex modulator in series with the first complex modulator, either the upper or lower frequency image near the second IF can be rejected.

TYPICAL PERFORMANCE CHARACTERISTICS

T_{MIN} to T_{MAX}, AVDD1, AVDD2 = 3.3 V, ACVDD, ADVDD, CLKVDD, DVDD, DRVDD = 2.5 V, I_{OUTFS} = 20 mA, differential transformer coupled output, 50 Ω doubly terminated, unless otherwise noted.

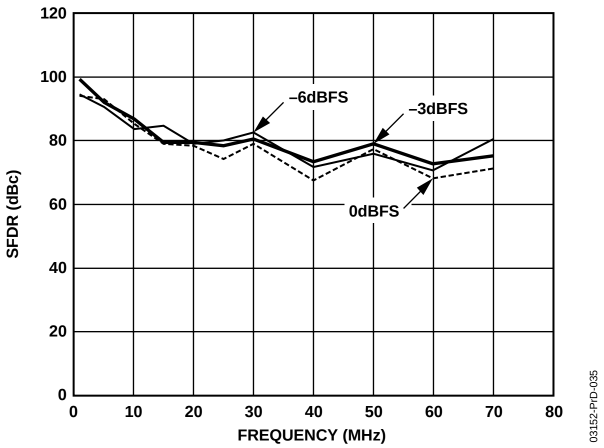


Figure 3. SFDR vs. Frequency, F_{DATA} = 200 MSPS, 1× Interpolation

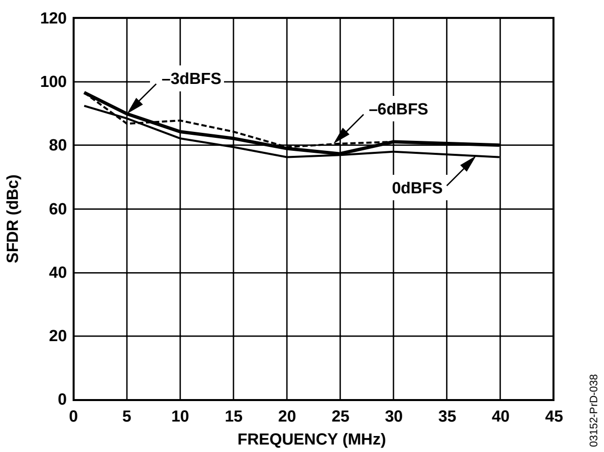


Figure 4. SFDR vs. Frequency, F_{DATA} = 100 MSPS, 4× Interpolation

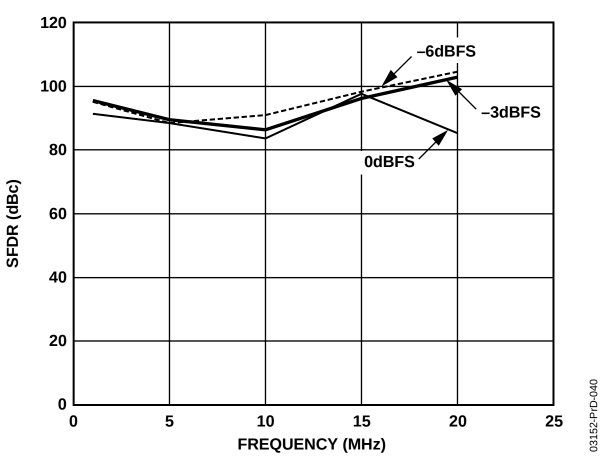


Figure 5. SFDR vs. Frequency, F_{DATA} = 50 MSPS, 8× Interpolation

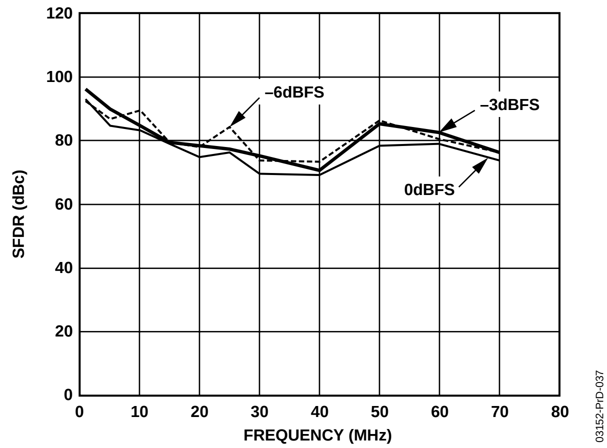


Figure 6. SFDR vs. Frequency, F_{DATA} = 200 MSPS, 2× Interpolation

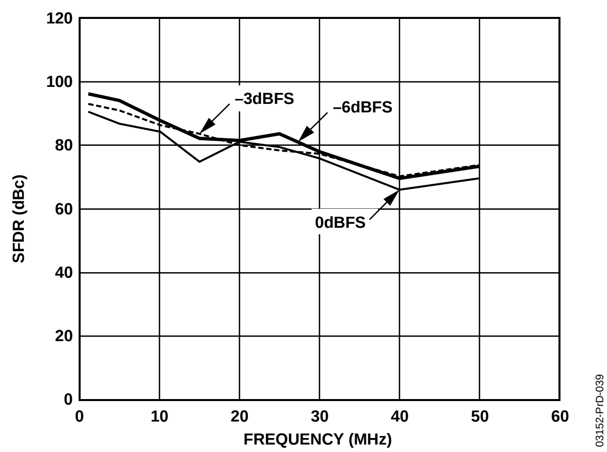


Figure 7. SFDR vs. Frequency, F_{DATA} = 125 MSPS, 4× Interpolation

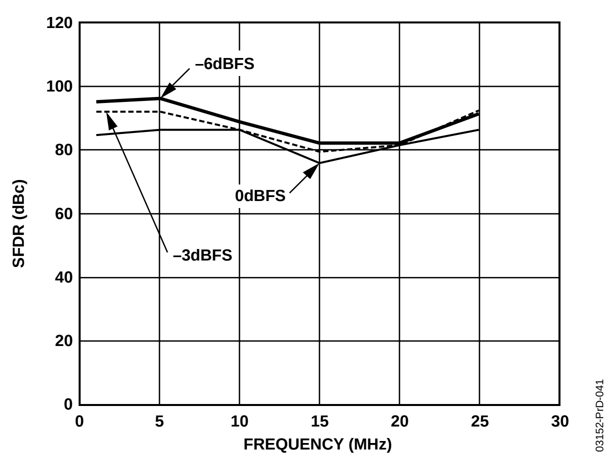


Figure 8. SFDR vs. Frequency, F_{DATA} = 62.5 MSPS, 8× Interpolation

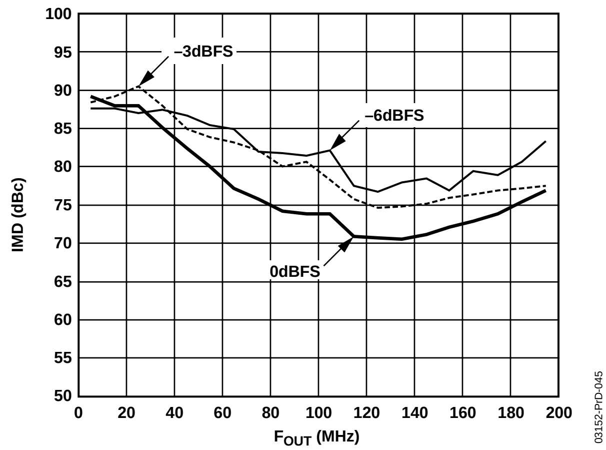


Figure 9. Out of Band SFDR, F_{DATA} = 200 MSPS, 2× Interpolation

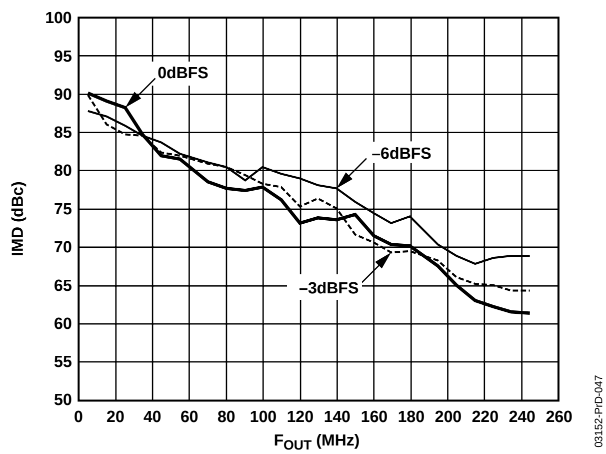


Figure 10. Out of Band SFDR, F_{DATA} = 125 MSPS, 4× Interpolation

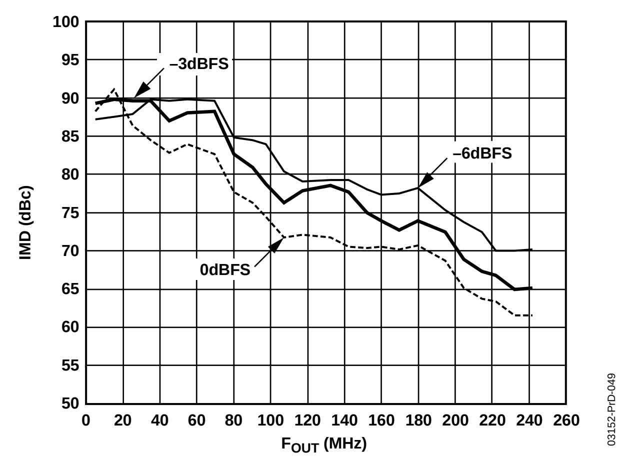


Figure 11. Out of Band SFDR, F_{DATA} = 62.5 MSPS, 8× Interpolation

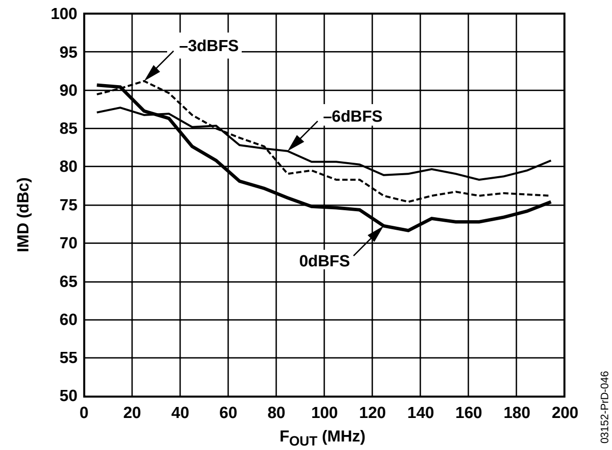


Figure 12. Out of Band SFDR, F_{DATA} = 100 MSPS, 4× Interpolation

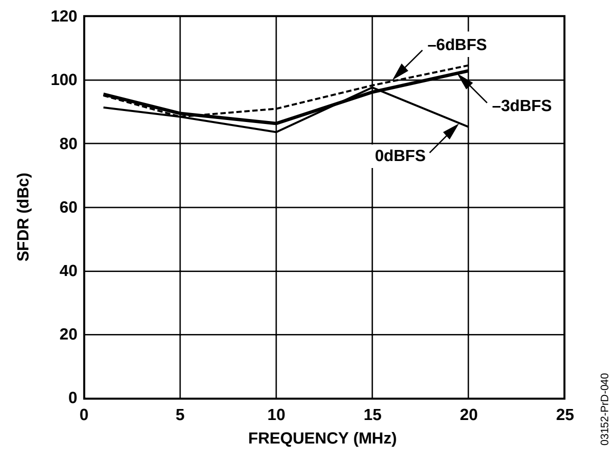


Figure 13. Out of Band SFDR, F_{DATA} = 50 MSPS, 8× Interpolation

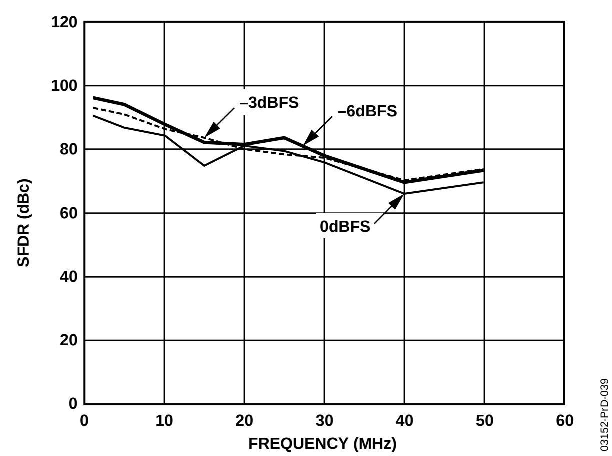


Figure 14. Third Order IMD vs. Frequency, F_{DATA} = 160 MSPS, 1× Interpolation

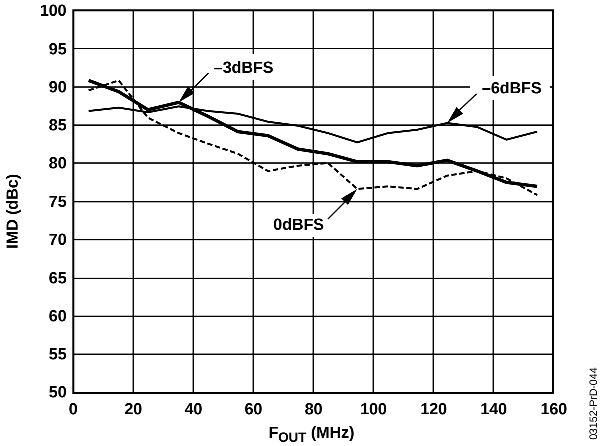


Figure 15. Third Order IMD vs. Frequency, F_{DATA} = 160 MSPS, 2× Interpolation

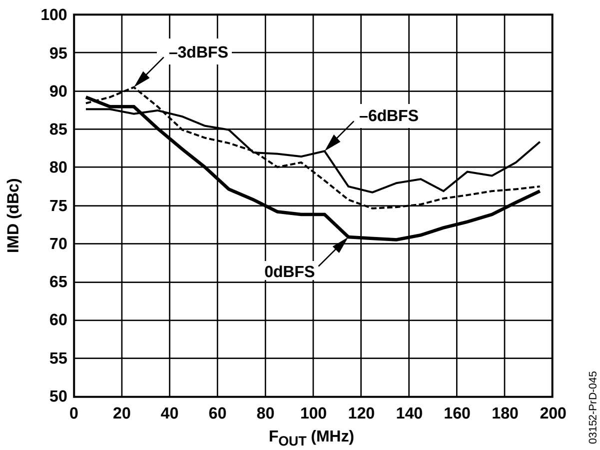


Figure 16. Third Order IMD vs. Frequency, F_{DATA} = 200 MSPS, 2× Interpolation

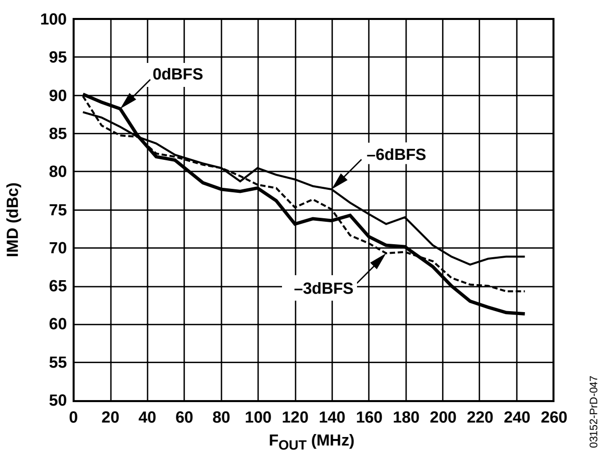


Figure 17. Third Order IMD vs. Frequency, F_{DATA} = 125 MSPS, 4× Interpolation

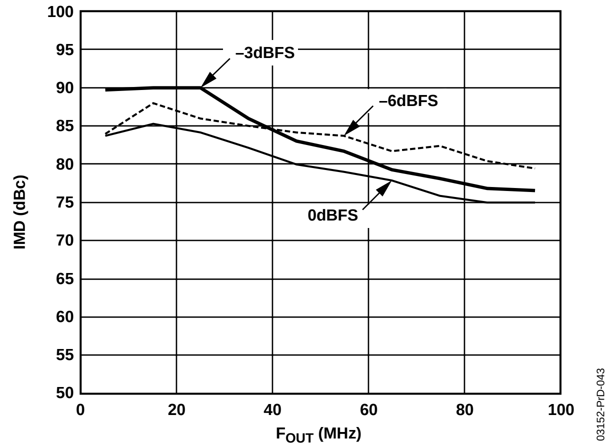


Figure 18. Third Order IMD vs. Frequency, F_{DATA} = 200 MSPS,1x Interpolation

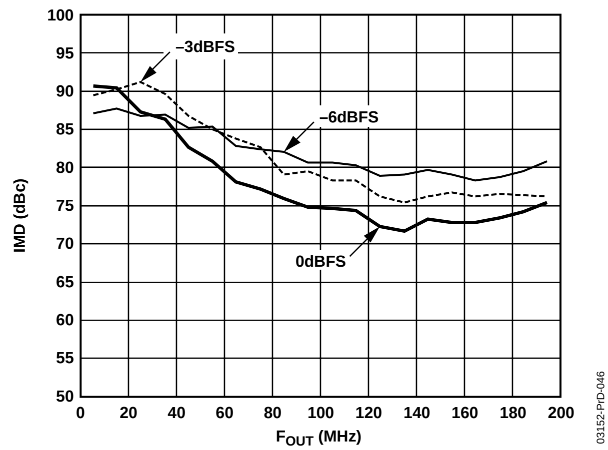


Figure 19. Third Order IMD vs. Frequency, F_{DATA} = 100 MSPS, 4× Interpolation

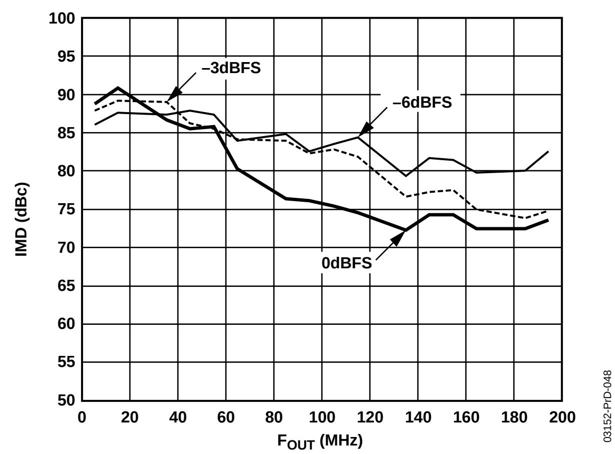


Figure 20. Third Order IMD vs. Frequency, F_{DATA} = 50 MSPS, 8× Interpolation

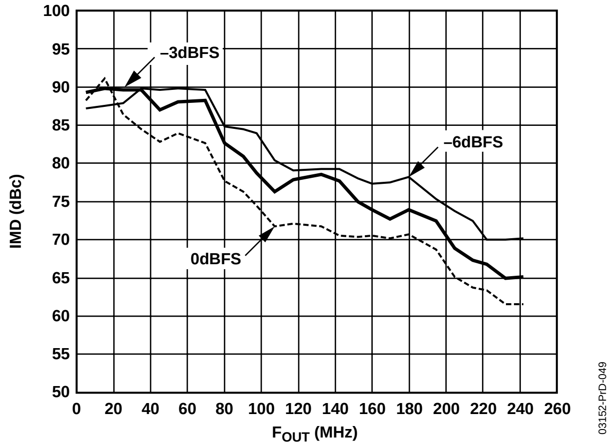


Figure 21. Third Order IMD vs. Frequency, F_{DATA} = 62.5 MSPS, 8× Interpolation

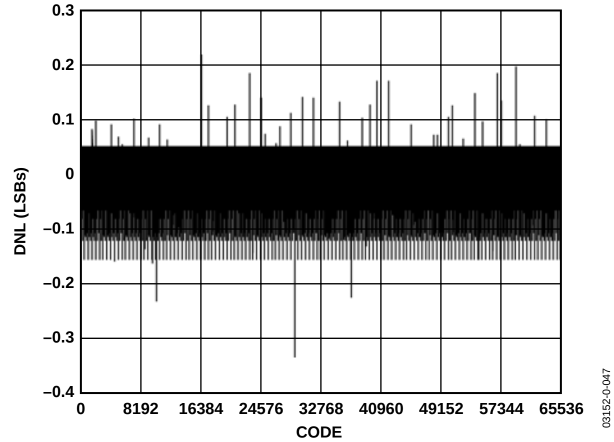


Figure 24. Typical DNL

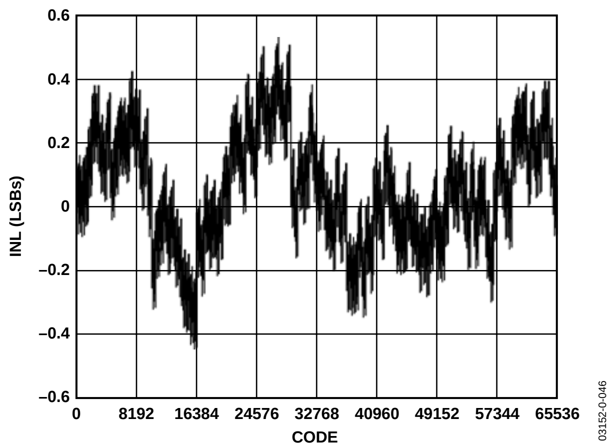


Figure 22. Typical INL

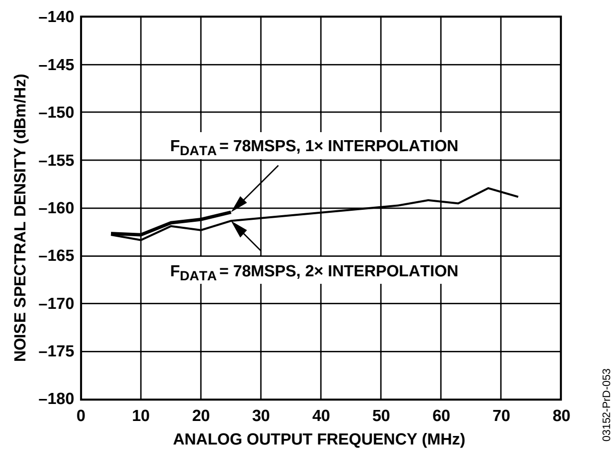


Figure 25. Noise Spectral Density vs. Analog Input Frequency, F_{DATA} = 78 MSPS, Interpolation = 1x

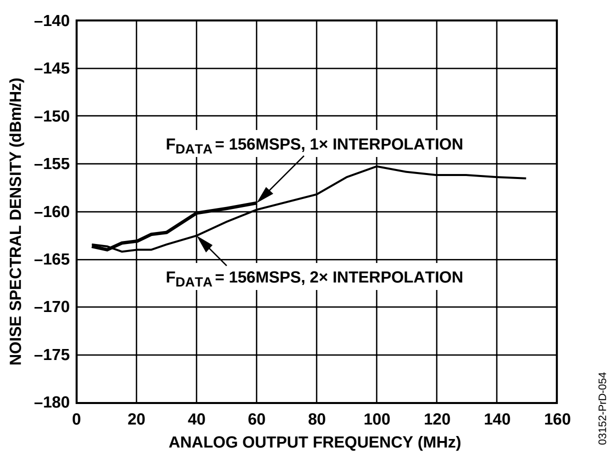


Figure 23. Noise Spectral Density vs. Analog Input Frequency, F_{DATA} = 156 MSPS, Interpolation = 1x

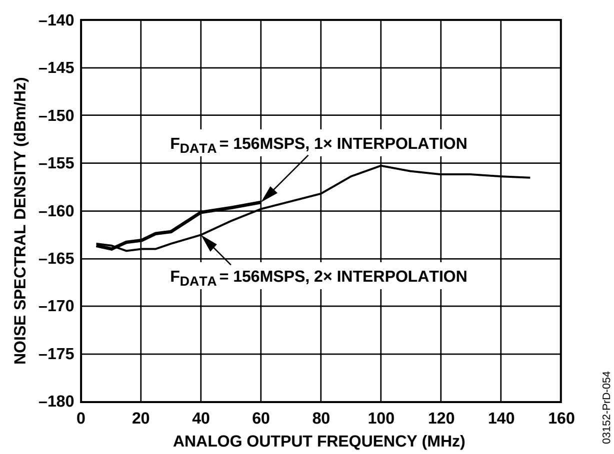


Figure 26. Noise Spectral Density vs. Analog Input Frequency, F_{DATA} = 78 MSPS Interpolation = 2x

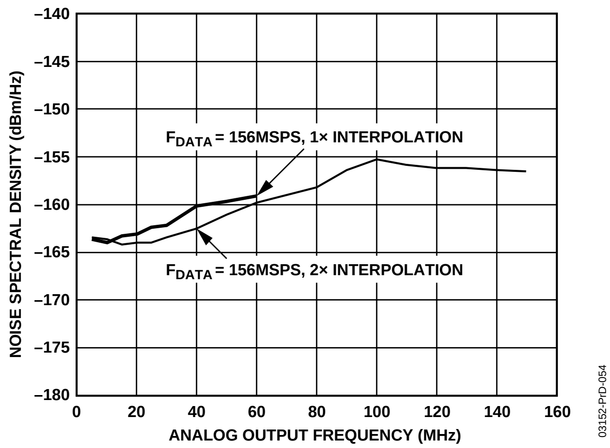


Figure 27. Noise Spectral Density vs. Analog Input Frequency, F_{DATA} = 156 MSPS Interpolation = 2x

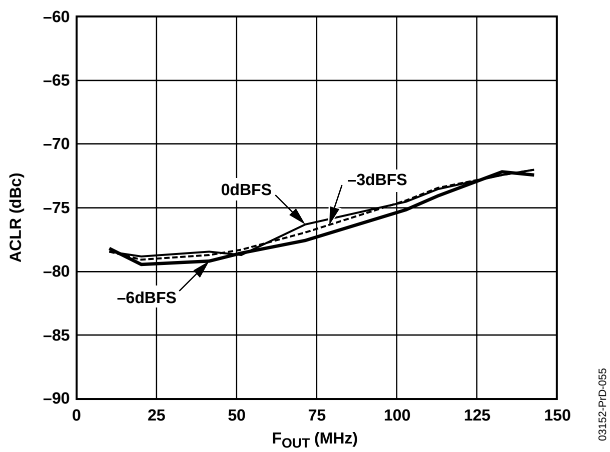


Figure 28. ACLR for First Adjacent Band vs. Frequency, F_{DATA} = 61.44 MSPS, 4× Interpolation

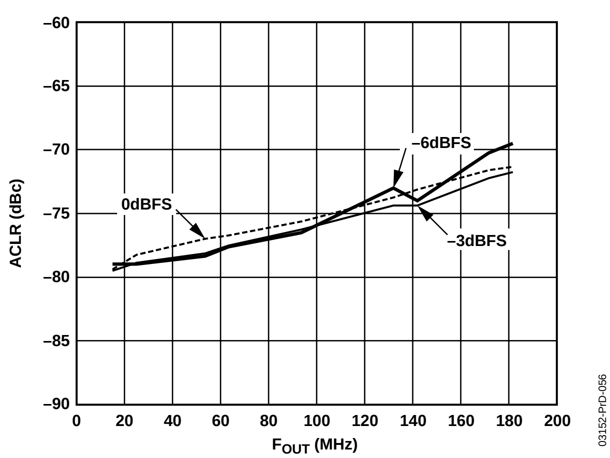


Figure 29. ACLR for First Adjacent Band vs. Frequency, F_{DATA} = 76.8 MSPS, 4× Interpolation

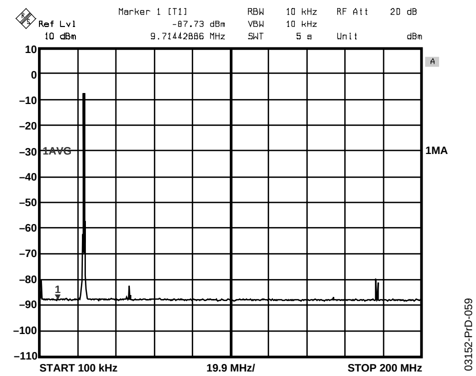


Figure 30. Two Tones around 23 MHz, F_{DATA} = 200 MSPS, 2× Interpolation, Low-Pass Digital Filter Mode

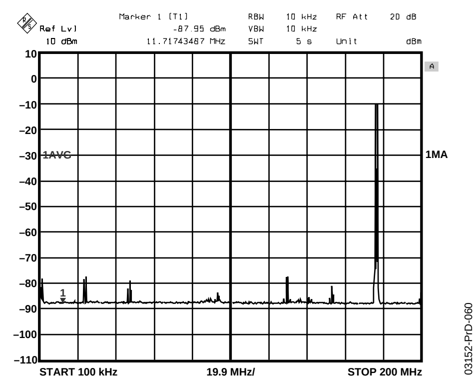


Figure 31. Two Tones around 177 MHz, F_{DATA} = 200 MSPS, 2× Interpolation, High-Pass Digital Filter Mode

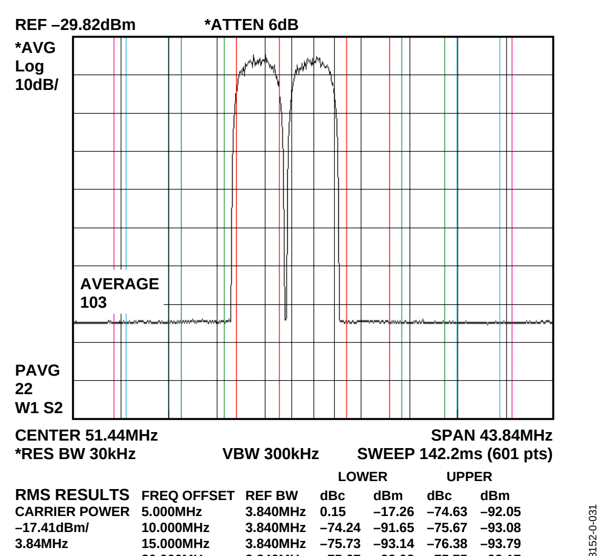


Figure 32. ACLR for Two WCDMA Carriers at 51.44 MHz, F_{DATA} = 61.44 MSPS, 4× Interpolation

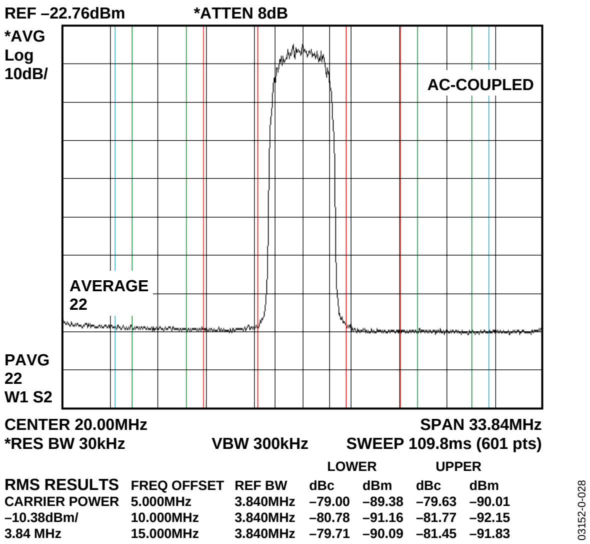


Figure 33. ACLR for Single WCDMA Carrier at 20 MHz, F_{DATA} = 61.44 MSPS, 4× Interpolation

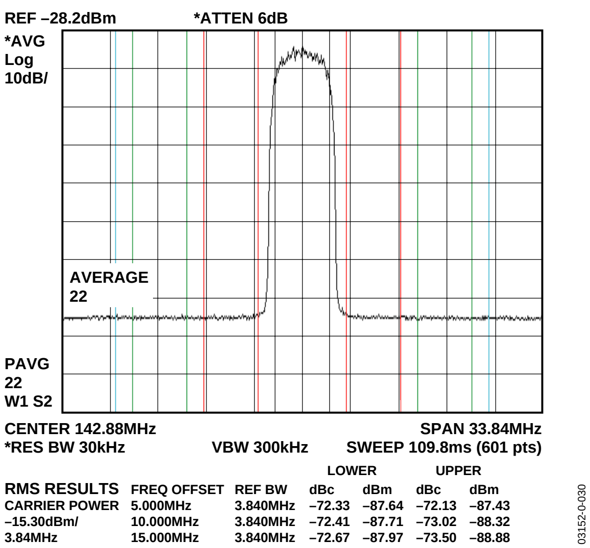


Figure 34. ACLR for Single WCDMA Carrier at 142.88 MHz, F_{DATA} = 61.44 MSPS, 4× Interpolation

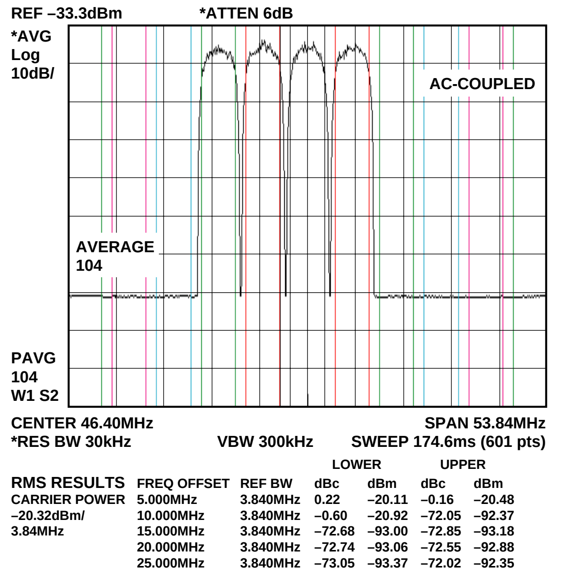


Figure 35. ACLR for Four-Carrier WCDMA Signal Near 50 MHz, F_{DATA} = 61.44 MSPS, 4× Interpolation

SERIAL CONTROL INTERFACE

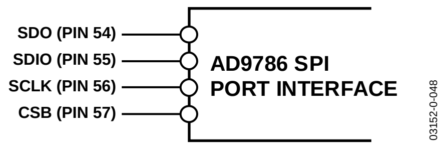


Figure 36. AD9786 SPI Port Interface

The AD9786 serial port is a flexible, synchronous serial communications port, allowing easy interface to many industry-standard microcontrollers and microprocessors. The serial I/O is compatible with most synchronous transfer formats, including both the Motorola SPI® and Intel® SSR protocols. The interface allows read/write access to all registers that configure the AD9786. Single or multiple byte transfers are supported, as well as MSB first or LSB first transfer formats. The AD9786's serial interface port can be configured as a single pin I/O (SDIO) or two unidirectional pins for in/out (SDIO/SDO).

GENERAL OPERATION OF THE SERIAL INTERFACE

There are two phases to a communication cycle with the AD9786. Phase 1 is the instruction cycle, which is the writing of an instruction byte into the AD9786, coincident with the first eight SCLK rising edges. The instruction byte provides the AD9786 serial port controller with information regarding the data transfer cycle, which is Phase 2 of the communication cycle. The Phase 1 instruction byte defines whether the upcoming data transfer is read or write, the number of bytes in the data transfer, and the starting register address for the first byte of the data transfer. The first eight SCLK rising edges of each communication cycle are used to write the instruction byte into the AD9786.

A logic high on the CS pin, followed by a logic low, will reset the SPI port timing to the initial state of the instruction cycle. This is true regardless of the present state of the internal registers or the other signal levels present at the inputs to the SPI port. If the SPI port is in the midst of an instruction cycle or a data transfer cycle, none of the present data will be written.

The remaining SCLK edges are for Phase 2 of the communication cycle. Phase 2 is the actual data transfer between the AD9786 and the system controller. Phase 2 of the communication cycle is a transfer of 1, 2, 3, or 4 data bytes as determined by the instruction byte. Using one multibyte transfer is the preferred method. Single byte data transfers are useful to reduce CPU overhead when register access requires one byte only. Registers change immediately upon writing to the last bit of each transfer byte.

Instruction Byte

The instruction byte contains the following information:

Table 9.

N1	N2	Description
0	0	Transfer 1 Byte
0	1	Transfer 2 Bytes
1	0	Transfer 3 Bytes
1	1	Transfer 4 Bytes

R/W, Bit 7 of the instruction byte, determines whether a read or a write data transfer will occur after the instruction byte write. Logic high indicates read operation. Logic 0 indicates a write operation. N1, N0, Bits 6 and 5 of the instruction byte, determine the number of bytes to be transferred during the data transfer cycle. The bit decodes are shown in Table 10.

Table 10.

MSB							LSB
I7	I6	I5	I4	I3	I2	I1	I0
R/W	N1	N0	A4	A3	A2	A1	A0

A4, A3, A2, A1, A0, Bits 4, 3, 2, 1, 0 of the instruction byte, determine which register is accessed during the data transfer portion of the communications cycle. For multibyte transfers, this address is the starting byte address. The remaining register addresses are generated by the AD9786.

SERIAL INTERFACE PORT PIN DESCRIPTIONS

SCLK—Serial Clock. The serial clock pin is used to synchronize data to and from the AD9786 and to run the internal state machines. SCLK's maximum frequency is 20 MHz. All data input to the AD9786 is registered on the rising edge of SCLK. All data is driven out of the AD9786 on the falling edge of SCLK.

CSB—Chip Select. Active low input starts and gates a communication cycle. It allows more than one device to be used on the same serial communications lines. The SDO and SDIO pins will go to a high impedance state when this input is high. Chip select should stay low during the entire communication cycle.

SDIO—Serial Data I/O. Data is always written into the AD9786 on this pin. However, this pin can be used as a bidirectional data line. The configuration of this pin is controlled by Bit 7 of register address 00h. The default is Logic 0, which configures the SDIO pin as unidirectional.

SDO—Serial Data Out. Data is read from this pin for protocols that use separate lines for transmitting and receiving data. In the case where the AD9786 operates in a single bidirectional I/O mode, this pin does not output data and is set to a high impedance state.

MSB/LSB TRANSFERS

The AD9786 serial port can support both most significant bit (MSB) first or least significant bit (LSB) first data formats. This functionality is controlled by register address DATADIR (00h[6]). The default is MSB first. When this bit is set active high, the AD9786 serial port is in LSB first format. That is, if the AD9786 is in LSB first mode, the instruction byte must be written from least significant bit to most significant bit. Multibyte data transfers in MSB format can be completed by writing an instruction byte that includes the register address of the most significant byte. In MSB first mode, the serial port internal byte address generator decrements for each byte required of the multibyte communication cycle. Multibyte data transfers in LSB first format can be completed by writing an instruction byte that includes the register address of the least significant byte. In LSB first mode, the serial port internal byte address generator increments for each byte required of the multibyte communication cycle.

The AD9786 serial port controller address will increment from 1Fh to 00h for multibyte I/O operations if the MSB first mode is active. The serial port controller address will decrement from 00h to 1Fh for multibyte I/O operations if the LSB first mode is active.

NOTES ON SERIAL PORT OPERATION

The AD9786 serial port configuration bits reside in Bits 6 and 7 of register address 00h. It is important to note that the configuration changes immediately upon writing to the last bit of the register. For multibyte transfers, writing to this register may occur during the middle of communication cycle. Care must be taken to compensate for this new configuration for the remaining bytes of the current communication cycle.

The same considerations apply to setting the software reset, SWRST (00h[5]) bit. All other registers are set to their default values, but the software reset does not affect the bits in Register Address 00h and 04h.

It is recommended to use only single byte transfers when changing serial port configurations or initiating a software reset.

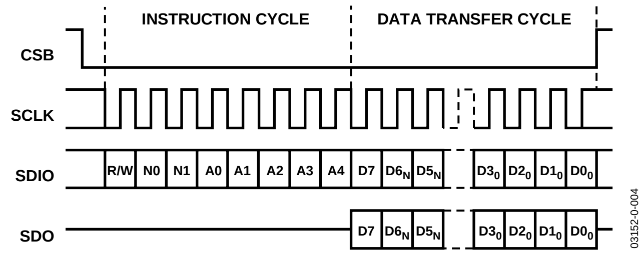


Figure 37. Serial Register Interface Timing MSB First

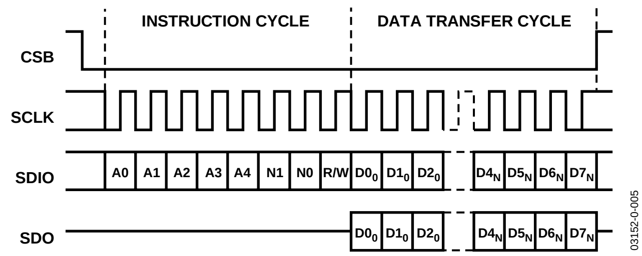


Figure 38. Serial Register Interface Timing LSB First

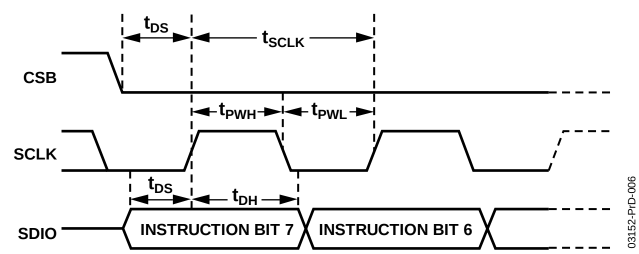


Figure 39. Timing Diagram for Register Write

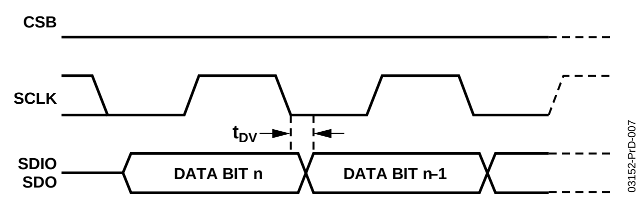


Figure 40. Timing Diagram for Register Read

MODE CONTROL (VIA SERIAL PORT)

Table 11.

Address		Bit 7	Bit 6	Bit 5	Bit 4	Bit 3	Bit 2	Bit 1	Bit 0
COMMS	00	SDIODIR	DATADIR	SWRST	SLEEP	PDN			EXREF
FILTER	01	INTERP[1]	INTERP[0]			ZSTUFF	HPFX8	HPFX4	HPFX2
DATA	02	DATAFMT	ONEPORT	DCLKSTR	DCLKPOL	DCLKEXT	DCLKCRC	IQPOL	CRAYDIN
MODULATE	03	CHANNEL	HILBERT	MODDUAL	SIDEBAND	MOD[1]	MOD[0]		
RESERVED	04	RESERVED	RESERVED	RESERVED	RESERVED	RESERVED	RESERVED	RESERVED	RESERVED
DCLKCRC	05	DATADJ[3]	DATADJ[2]	DATADJ[1]	DATADJ[0]	MODSYNC	MODADJ[2]	MODADJ[1]	MODADJ[0]
	06	Reserved							
	07	Reserved							
	08	Reserved							
	09	Reserved							
	0A	Reserved							
	0B	Reserved							
	0C	Reserved							
	0D	Reserved							
CALMEMCK	0E			CALMEM[1]	CALMEN[0]		CALCKDIV[2]	CALCKDIV[2]	CALCKDIV[2]
MEMRDWR	0F	CALSTAT	CALEN	XFERSTAT	XFEREN	SMEMWR	SMEMRD	FMEMRD	UNCAL
MEMADDR	10	MEMADDR[7]	MEMADDR[6]	MEMADDR[5]	MEMADDR[4]	MEMADDR[3]	MEMADDR[2]	MEMADDR[1]	MEMADDR[0]
MEMDATA	11			MEMDATA[5]	MEMDATA[4]	MEMDATA[3]	MEMDATA[2]	MEMDATA[1]	MEMDATA[0]
DCRCSTAT	12						DCRCSTAT[2]	DCRCSTAT[1]	DCRCSTAT[0]

Table 12.

COMMS(00)	Bit	Direction	Default	Description
SDIODIR	7	I	0	0: SDIO pin configured for input only during data transfer 1: SDIO configured for input or output during data transfer
DATADIR	6	I	0	0: Serial data uses MSB first format 1: Serial data uses LSB first format
SWRST	5	I	0	1: Default all serial register bits, except addresses 00h and 04h
SLEEP	4	I	0	1: DAC output current off
PDN	3	I	0	1: All analog and digital circuitry, except serial interface, off
EXREF	0	I	0	0: Internal band gap reference 1: External reference

Table 13.

FILTER(01)	Bit	Direction	Default	Description
INTERP[1:0]	[7:6]	I	00	00: No interpolation 01: Interpolation 2× 10: Interpolation 4× 11: Interpolation 8×
ZSTUFF	3	I	0	1: Zero Stuffing on
HPFX8	2	I	0	0: ×8 interpolation filter configured for low pass 1: ×8 interpolation filter configured for high pass
HPFX4	1	I	0	0: ×4 interpolation filter configured for low pass 1: ×4 interpolation filter configured for high pass
HPFX2	0	I	0	0: ×2 interpolation filter configured for low pass 1: ×2 interpolation filter configured for high pass

Table 14.

DATA(02)	Bit	Direction	Default	Description
DATAFMT	7	I	0	0: Twos complement data format 1: Unsigned binary input data format
ONEPORT	6	I	0	0: I and Q input data onto ports one and two, respectively 1: I and Q input data interleaved onto port one
DCLKSTR	5	I	0	0: DATACLK pin 12 mA drive strength 1: DATACLK pin 24 mA drive strength
DCLKPOL	4	I	0	0: Input data latched on DATACLK rising edge 1: Input data latched on DATACLK falling edge
DCLKEXT	3	I	0	0: DATACLK pin inputs channel data rate or modulator synchronizer clock 1: DATACLK pin outputs channel data rate or modulator synchronizer clock
DCLKCRC	2	I	0	0: With DATACLK pin as input, DATACLK clock recovery off 1: With DATACLK pin as input, DATACLK clock recovery on
IQPOL	1	I	0	0: In one port mode, IQSEL = 1 latches data into I channel, IQSEL = 0 latches data into Q channel 1: In one port mode, IQSEL = 0 latches data into I channel, IQSEL = 1 latches data into Q channel
GRAYDIN	0	I	0	0: Gray decoder off 1: Gray decoder on

Table 15.

MODULATE(03)	Bit	Direction	Default	Description		
CHANNEL	7	I	0	**MODDUAL 03h [5]**	**CHANNEL 03h[7]**	
				0	0	I channel processing routed to DAC
				0	1	Q channel processing routed to DAC
				1	0	Modulator real output routed to DAC
				1	1	Modulator imaginary output routed to DAC
HILBERT	6	I	0	1: With MODDUAL on, Hilbert transform on		
MODDUAL	5	I	0	0: Modulator uses a single channel 1: Modulator uses both I and Q channels		
SIDEBAND	4	I	0	0: With MODDUAL on, lower sideband rejected 1: With MODDUAL on, upper sideband rejected		
MOD[1:0]	[3:2]	I	00	00: No modulation 01: $f_S/2$ modulation 10: $f_S/4$ modulation 11: $f_S/8$ modulation		

Table 16.

<table>
<tr><th>DCLKCRC(05)</th><th>Bit</th><th>Direction</th><th>Default</th><th>Description</th></tr>
<tr><td>DATADJ[3:0]</td><td>[7:4]</td><td>I</td><td>0000</td><td>DATACLK offset. Twos complement representation
0111: +7
:
0000: 0
:
1000: -8</td></tr>
<tr><td>MODSYNC</td><td>3</td><td>I</td><td>00</td><td>0: Channel data rate clock synchronizer mode
1: State machine clock synchronizer mode</td></tr>
<tr><td>MODADJ[2:0]</td><td>[2:0]</td><td>I</td><td>000</td><td><table>
<tr><th></th><th>$f_S/8$</th><th>$f_S/4$</th><th>$f_S/2$</th><th>Modulator coefficient offset</th></tr>
<tr><td>000</td><td>1</td><td>1</td><td>1</td><td></td></tr>
<tr><td>001</td><td>1/√2</td><td>0</td><td>−1</td><td></td></tr>
<tr><td>010</td><td>0</td><td>−1</td><td>1</td><td></td></tr>
<tr><td>011</td><td>−1/√2</td><td>0</td><td>−1</td><td></td></tr>
<tr><td>100</td><td>−1</td><td>1</td><td>1</td><td></td></tr>
<tr><td>101</td><td>−1/√2</td><td>0</td><td>−1</td><td></td></tr>
<tr><td>110</td><td>0</td><td>−1</td><td>1</td><td></td></tr>
<tr><td>111</td><td>1/√2</td><td>0</td><td>−1</td><td></td></tr>
</table></td></tr>
</table>

Table 17.

VERSION(0D)	Bit	Direction	Default	Description
VERSION[3:0]	[3:0]	O		Hardware version identifier

Table 18.

CALMEMCK(OE)	Bit	Direction	Default	Description
CALMEM	[5:4]	O	00	Calibration memory 00: Uncalibrated 01: Self calibration 10: Factory calibration 11: User input
CALCKDIV[2:0]	[2:0]	I	00	Calibration clock divide ratio from channel data rate 000: /32 001: /64 : 110: /2048 111: /4096

Table 19.

MEMRDWR(OF)	Bit	Direction	Default	Description
CALSTAT	7	O	0	0: Self calibration cycle not complete 1: Self calibration cycle complete
CALEN	6	I	0	1: Self calibration in progress
XFERSTAT	5	O	0	0: Factory memory transfer not complete 1: Factory memory transfer complete
XFEREN	4	I	0	1: Factory memory transfer in progress
SMEMWR	3	I	0	1: Write static memory data from external port
SMEMRD	2	I	0	1: Read static memory to external port
FMEMRD	1	I	0	1: Read factory memory data to external port
UNCAL	0	I	0	1: Use uncalibrated

Table 20.

MEMADDR(10)	Bit	Direction	Default	Description
MEMADDR [7:0]	[7:0]	I/O	00000000	Address of factory or static memory to be accessed

Table 21.

MEMDATA(11)	Bit	Direction	Default	Description
MEMDATA [5:0]	[5:0]	I/O	000000	Data or factory or static memory access

Table 22.

DCRCSTAT(12)	Bit	Direction	Default	Description
DCRCSTAT (2)	2	O	0	0: With DATACLK CRC on, lock has never been achieved. 1: With DATACLK CRC on, lock has been achieved at least once.
DCRCSTAT(1)	1	O	0	0: With DATACLK CRC on, system is currently not locked. 1: With DATACLK CRC on, system is currently locked.
DCRCSTAT(0)	0	O	0	0: With DATACLK CRC on, system is currently locked. 1: With DATACLK CRC on, system lost lock due to jitter.

DIGITAL FILTER SPECIFICATIONS

DIGITAL INTERPOLATION FILTER COEFFICIENTS

Table 23. Stage 1 Interpolation Filter Coefficients

Lower Coefficient	Upper Coefficient	Integer Value
H(1)	H(43)	9
H(2)	H(42)	0
H(3)	H(41)	–27
H(4)	H(40)	0
H(5)	H(39)	65
H(6)	H(38)	0
H(7)	H(37)	–131
H(8)	H(36)	0
H(9)	H(35)	239
H(10)	H(34)	0
H(11)	H(33)	–407
H(12)	H(32)	0
H(13)	H(31)	665
H(14)	H(30)	0
H(15)	H(29)	–1070
H(16)	H(28)	0
H(17)	H(27)	1764
H(18)	H(26)	0
H(19)	H(25)	–3273
H(20)	H(24)	0
H(21)	H(23)	10358
H(22)		16384

Table 24. Stage 2 Interpolation Filter Coefficients

Lower Coefficient	Upper Coefficient	Integer Value
H(1)	H(19)	19
H(2)	H(18)	0
H(3)	H(17)	–120
H(4)	H(16)	0
H(5)	H(15)	436
H(6)	H(14)	0
H(7)	H(13)	–1284
H(8)	H(12)	0
H(9)	H(11)	5045
H(10)		8192

Table 25. Stage 3 Interpolation Filter Coefficients

Lower Coefficient	Upper Coefficient	Integer Value
H(1)	H(11)	7
H(2)	H(10)	0
H(3)	H(9)	–53
H(4)	H(8)	0
H(5)	H(7)	302
H(6)		512

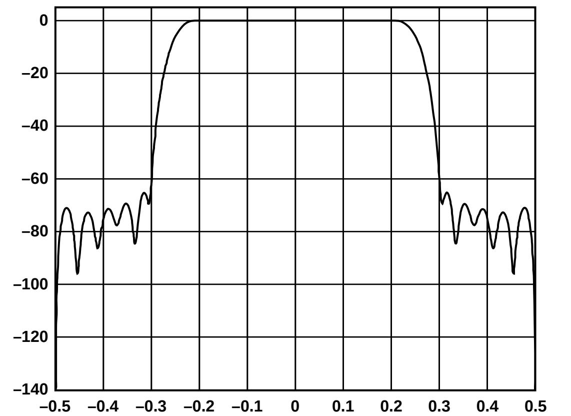


Figure 41. ×2 Interpolation Filter Response

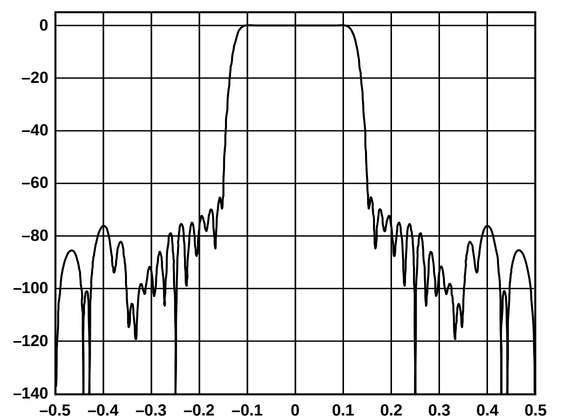


Figure 42. ×4 Interpolation Filter Response

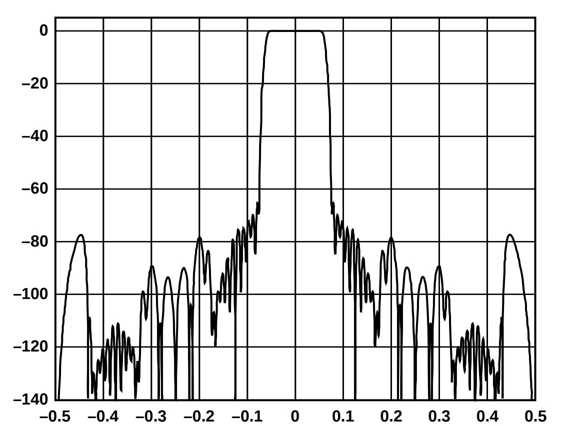


Figure 43. ×8 Interpolation Filter Response

AD9786 CLOCK/DATA TIMING

Table 26. Data Port Synchronization

DCLKEXT 02h, Bit 3	MODSYNC 05h, Bit 3	DCLKCRC 02h, Bit 2	Mode	Function
1	0	X	DATACLK Master	Channel data rate clock output
1	1	X	Modulator Master	Modulator synchronization DATACLK output
0	0	0	External Sync Mode	DATACLK inactive, DACCLK synchronous with external data
0	0	1	DATACLK Slave	DATACLK input, data rate clock, Data Recovery On
0	1	0	Low Setup/Hold	DATACLK input, input data synchronous with DATACLK
0	1	1	Modulator Slave	Input modulator synchronizer DATACLK input

Two-Port Data Input Mode, DATACLK Master

With the interpolation set to 1×, the DATACLK output is a delayed and inverted version of DACCLK at the same frequency. Note that DACCLK refers to the differential clock inputs applied at Pins 5 and 6. As Figure 44 and Figure 45 show, there is a constant delay between the edges of DACCLK and DATACLK.

The DCLKPOL bit (Reg 02 Bit 4) allows the data to be latched into the AD9786 on either the rising or falling edge of DACCLK. With DCLKPOL = 0, the data is latched in on the falling edge of DACCLK, as shown in Figure 44. With DCLKPOL = 1, as shown in Figure 45, data is latched in on the rising edge of DACCLK. The setup and hold times are always with respect to the latching edge of DACCLK.

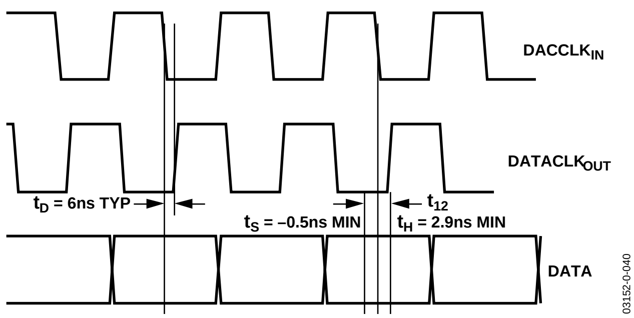


Figure 44. Data Timing, 1× Interpolation, DCLKPOL = 0

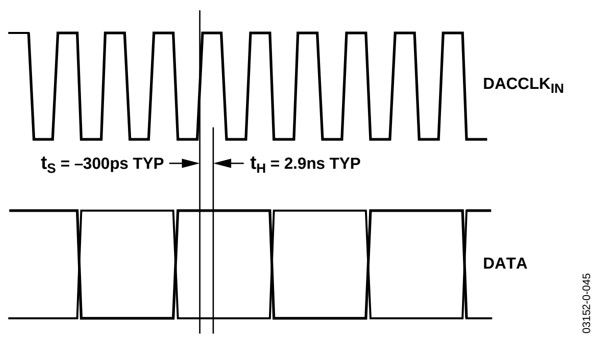


Figure 45. Data Timing, 1× Interpolation, DCLKPOL = 1

With the interpolation set to 2×, the DACCLK input runs at twice the speed of the DATACLK. Data is latched into the digital inputs of the AD9786 on every other rising edge of DACCLK, as shown in Figure 47 and Figure 48. With DCLKPOL = 0, as shown in Figure 47, the latching edge of DACCLK is the rising edge that occurs just before the falling edge of DATACLK. With DCLKPOL = 1, as in Figure 48, the latching edge of DACCLK is the rising edge of DACCLK that occurs just before the rising edge of DATACLK. The setup and hold time values are identical to those in Figure 44 and Figure 45.

Note that there is a slight difference in the delay from the rising edge of DACCLK to the falling edge of DATACLK, and the delay from the rising edge of DACCLK to the rising edge of DATACLK. As Figure 46 shows, the DATACLK duty cycle is slightly less than 50%. This is true in all modes.

With the interpolation set to 4× or 8×, the DACCLK input runs at 4× or 8× the speed of the DATACLK output. The data is latched in on a rising edge of DACCLK, similar to the 2× interpolation mode. However, the latching edge is every fourth edge in 4× interpolation mode and every eighth edge in the 8× interpolation mode. Similar to operation in the 2× interpolation mode, with DCLKPOL = 0, the latching edge of DACCLK is the rising edge that occurs just before the falling edge of DATACLK. With DCLKPOL = 1, the latching edge of DACCLK is the rising edge that occurs just before the rising edge of DATACLK. The setup and hold time values are identical to those in 1× and 2× interpolation.

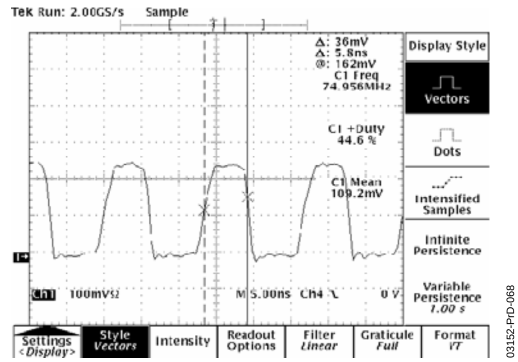


Figure 46.

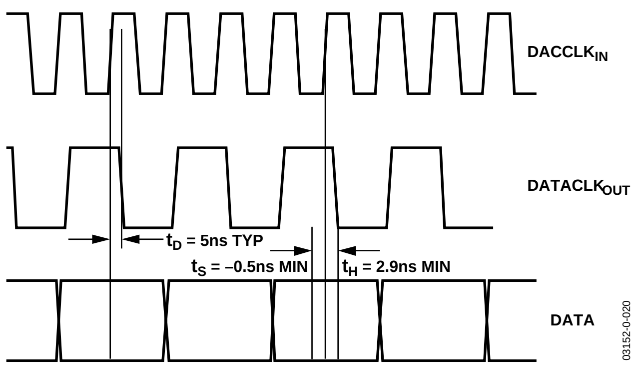


Figure 47. Data Timing, 2× Interpolation, DCLKPOL = 0

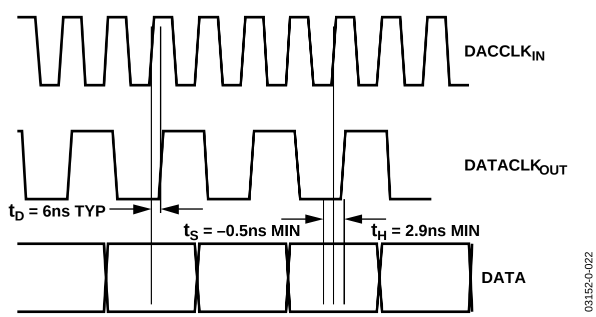


Figure 48. Data Timing, 2× Interpolation, DCLKPOL = 1

AD9786 DATACLK Slave Mode, Data Recovery On

DATACLK (Pin 31) can be used as an input in order to synchronize multiple AD9786s. A clock generated by an AD9786 operating in master mode, or a clock from an external source, can be used to drive DATACLK.

In this mode, there are two clocks required to be applied to the AD9786. A clock running at the DAC sample rate, referred to as DACCLK, must be applied to the differential inputs (Pins 5 and 6) of the AD9786. As described above, a clock at the input sample rate must also be applied to Pin 31 (DATACLK). An internal DLL synchronizes the two applied clocks. The timing relationships between the input data, DATACLK, and DACCLK are given in Figure 49 and Figure 50.

Note that DCLKPOL (Reg 02h, Bit 4) can be used to select the edge of DACCLK upon which the input data is latched.

There is a defined setup and hold window with respect to input data and the latching edge of DACCLK. There is also a required timing relationship between DATACLK and DACCLK. This is referred to in Figure 49 and Figure 50 as t_{ST} and t_{HT} (setup and hold for transition). As an example, with DCLKPOL set to logic 0, the input data will latch on the first rising edge of DACCLK which occurs greater than 1.5 ns before the falling edge of DATACLK. DACCLK should not be given a rising edge in the window of 500 ps to 1.5 ns before the latching edge (falling when DCLKPOL = 0, rising when DCLKPOL = 1) of DATACLK. Failure to account for this timing relationship may result in corrupt data.

There are three status bits available for read which allow the user to verify DLL lock. These are Bits 0, 1, and 2 (DCRCSTAT) in Reg 12h.

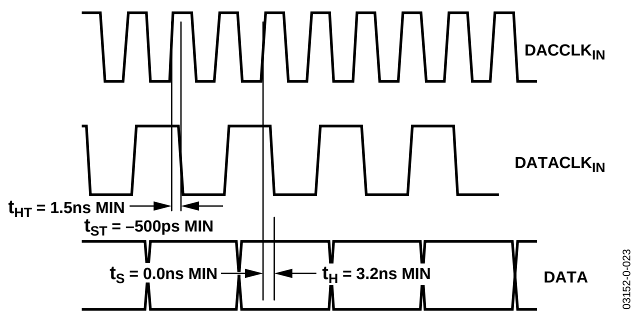


Figure 49. Slave Mode Timing, 2× Interpolation, DCLKPOL = 0

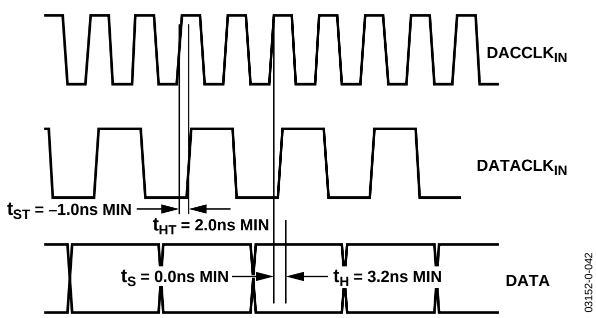


Figure 50. Slave Mode Timing, 2× Interpolation, DCLKPOL = 1

AD9786 Low Setup/Hold Mode (DATACLK input, data recovery off)

Some applications may require that digital input data be synchronized with the DATACLK input, rather than DACCLK. For these applications, the AD9786 can be programmed for Low Setup/Hold Mode by entering the values in Table 26 into the SPI registers. With data recovery off and the MODSYNC bit set to logic 1, the AD9786 will latch data in on the rising or falling edge of DATACLK input, depending on the state of DCLKPOL.

The timing is similar to the slave mode with data recovery on. There is still a required timing relationship between DACCLK and DATACLK in, as shown in Figure 51 and Figure 52. As these show, the digital input data is latched in on the DATACLK edge, rather than DACCLK. One advantage of this mode is that the setup and hold numbers for the input data with respect to DATACLK are much smaller than the similar specs in the slave/clock recovery mode.

Note that in this mode, the DATAADJ bits have no effect.

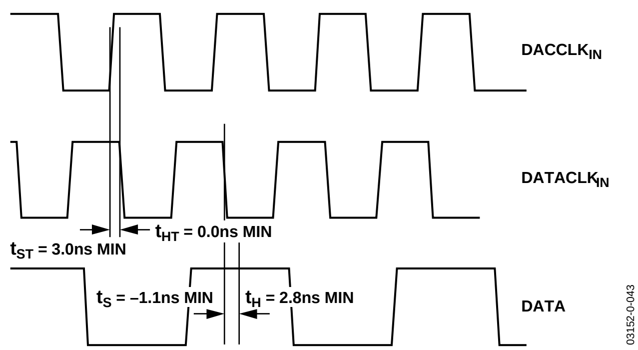


Figure 51. Low Setup and Hold Mode Timing, 2× Interpolation, DCLKPOL = 0

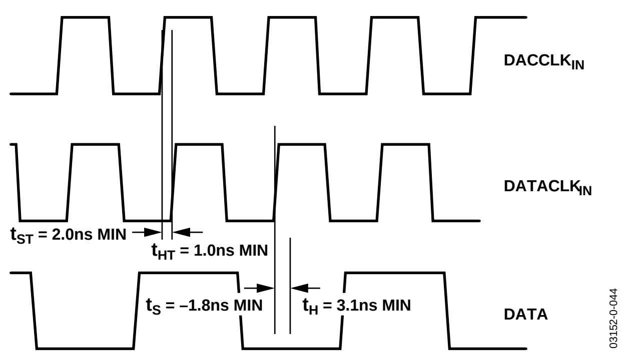


Figure 52. Low Setup and Hold Mode Timing, 2× Interpolation, DCLKPOL = 1

AD9786 External Sync Mode

There is one additional timing mode in which the AD9786 may be used. In the External Sync Mode, the DATACLK is programmed as an input, but is not used. Applying a DATACLK input while in this mode will have no effect. The digital input data is synchronized solely to the DACCLK input. With 1× interpolation, this means that the data input will be latched on every rising edge of DACCLK. The challenge is that the user has no way of knowing exactly which edge is the latching edge when the interpolating filters are in use. In 2×, 4×, and 8× interpolation modes, the latching edge of DACCLK will be either every 2nd, 4th, or 8th edge, respectively.

With the 2 ns keep out window, as shown in Figure 53, there is a strong possibility of violating setup and hold times, especially at high speeds. It is recommended that users sense the DAC output noise floor for setup and hold violations. If setup and hold is violated, DCLKPOL can be switched. The effect of switching the state of DCLKPOL is that the latching edge will be moved by one, two, or four DACCLK cycles if the AD9786 is in 2×, 4×, or 8× interpolation modes, respectively.

Note that in this mode, the DATAADJ bits have no effect.

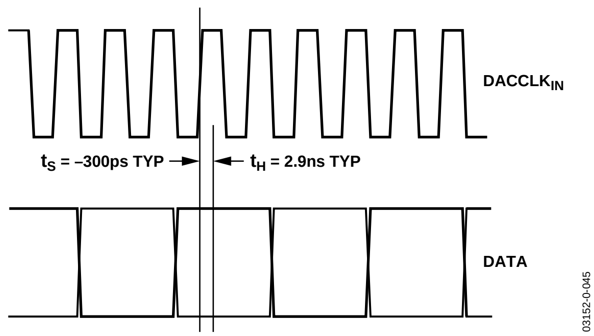


Figure 53. External Sync Mode with 2× Interpolation

DATAADJUST Synchronization

When designing the digital interface for high speed DACs, care must be taken to ensure that the DAC input data meets setup and hold requirements. Often, compensation must be used in the clock delay path to the digital engine driving the DAC. The AD9786 has the on-chip capability to vary the latching edge of DACCLK. With the interpolation function enabled, this allows the user the choice of multiple edges upon which to latch the data. For instance, if the AD9786 is using 8× interpolation, the user may latch from one of eight edges before the rising edge of DATACLK, or seven edges after this rising edge. The specific edge upon which data is latched is controlled by SPI Register 05h, Bits 7:4. Table 27 shows the relationship of the latching edge of DACCLK and DATACLK with the various settings of the DATAADJ bits.

Table 27. DATAADJ Values for Latching Edge Sync

SPI Reg 05h				
Bit 7	**Bit 6**	**Bit 5**	**Bit 4**	**Latching Edge wrt DATACLK**
0	0	0	0	0
0	0	0	1	+1
0	0	1	0	+2
0	0	1	1	+3
0	1	0	0	+4
0	1	0	1	+5
0	1	1	0	+6
0	1	1	1	+7
1	0	0	0	–8
1	0	0	1	–7
1	0	1	0	–6
1	0	1	1	–5
1	1	0	0	–4
1	1	0	1	–3
1	1	1	0	–2
1	1	1	1	–1

Note that the data in Figure 44 to Figure 53 was taken with the DATAADJ default of 0000. With DCLKPOL = 0, the latching edge of DACCLK is just previous to the rising edge of DATACLK; with DCLKPOL = 1, the latching edge of DACCLK is just previous to the falling edge of DATACLK. Table 27 describes the values available for 8× interpolation which gives a choice of 16 edges to sync data. With 4× interpolation, there will be a choice of 8 edges, and the relevant values from Table 27 will be 0000, 0010, 0100, 0110, 1000, 1010, 1100, and 1110. These options will allow latching edge placement from +3 cycles to −4 cycles. In 2× interpolation, 4 edges will be available, and the relevant values from Table 27 will be 0000, 0100, 1000, and 1100. The choices for DATAADJ are diminished to +1 cycle to −2 cycles.

Figure 54, Figure 55, and Figure 56 show the alignment for the latching edge of DACCLK with 4× interpolation and different settings for DATAADJ. In Figure 54, the AD9786 is in DATACLK Master Mode. DATAADJ is set to 0000, with DCLKPOL set to 0 so that the latching edge of DACCLK is immediately before the rising edge of DATACLK. The data transitions shown in Figure 54 are synchronous with the DACCLK, so that DACCLK and input data are constant with respect to each other. The only visible change when DATAADJ is altered is that DATACLK moves, indicating the latching edge has moved as well. Note that in DATACLK Master Mode, when DATAADJ is altered, the latching edge with respect to DATACLK remains the same.

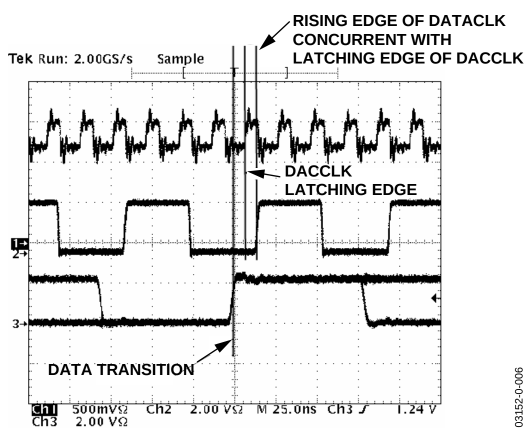


Figure 54. DATAADJ = 0000

Figure 55 shows the same conditions, but with DATAADJ set to 1111. This moves DATACLK to the left in the plot, indicating that it occurs one DACCLK cycle before it did in Figure 54. As explained previously, the latching edge of DACCLK also moves one cycle back in time.

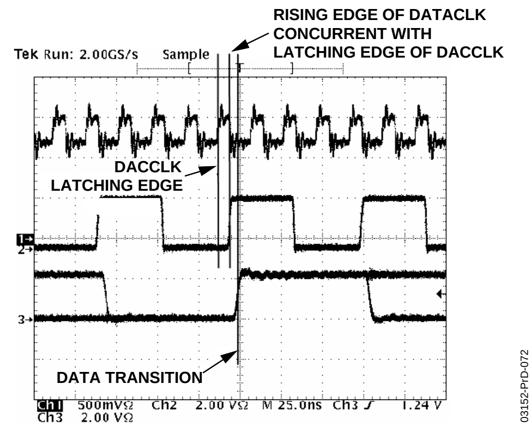


Figure 55. DATAADJ = 1111

Figure 56 shows the same conditions, with DATAADJ set to 0001, thus moving DATACLK to the right in the plot. This indicates that it occurs one DACCLK cycle after it did in Figure 54. In this case, the latching edge of DACCLK moves forward in time one cycle.

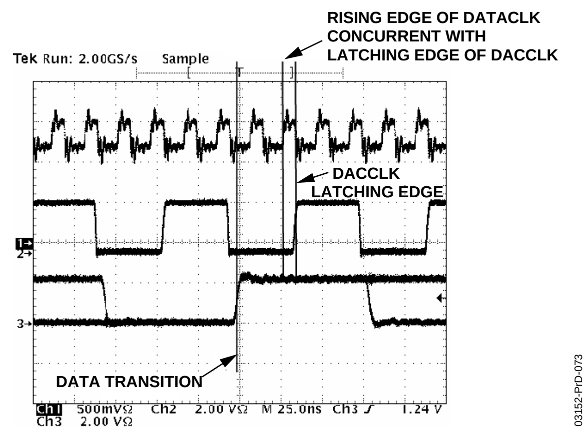


Figure 56. DATAADJ = 0001

Interpolation Modes

Table 28. Interpolation Modes

INTERP[1]	INTERP[0]	Mode
0	0	No Interpolation
0	1	×2 Interpolation
1	0	×4 Interpolation
1	1	×8 Interpolation

Interpolation is the process of increasing the number of points in a time domain waveform by approximating points between the input data points, on a uniform time grid. This produces a higher output data rate. Applied to an interpolation DAC, a digital interpolation filter is used to approximate the interpolated points, having an output data rate increased by the interpolation factor. Interpolation filter responses are achieved by cascading individual digital filter banks, whose filter coefficients are given in Table 23, Table 24, and Table 25. Filter responses are shown in Figure 57, which shows the interpolation filters of the AD9786 under different interpolation rates, normalized to the input data rate, f_{SIN}.

The digital filter's frequency domain response exhibits symmetry about half the output data rate and dc. It will cause images of the input data to be shaped by the interpolation filter's frequency response. This has the advantage of causing input data images, which fall in the stop band of the digital filter to be rejected by the stop-band attenuation of the interpolation filter; input data images falling in the interpolation filter's pass band will be passed. In band-limited applications, the images at the output of the DAC must be limited by an analog reconstruction filter. The complexity of the analog reconstruction filter is determined by the proximity of the closest image to the required signal band. Higher interpolation rates yield larger stop-band regions, suppressing more input images and resulting in a much relaxed analog reconstruction filter.

A DAC shapes its output with a sinc function, having a null at the sampling frequency of the DAC. The higher the DAC sampling rate compared to the input signal bandwidth, the less the DAC sinc function will shape the output. The higher the interpolation rate, the more input data images fall in the interpolation filter stop band and are rejected; the bandwidth between passed images is larger with higher interpolation factors. The sinc function shaping is also reduced with a higher interpolation factor.

Table 29. Sinc Shaping at Band Edge of Interpolation Filters

Mode	Sinc Shaping at $0.43f_{SIN}$ (dB)	Bandwidth to First Image
No Interpolation	−2.8241	f_{SIN}
×2 Interpolation	−0.6708	$2f_{SIN}$
×4 Interpolation	−0.1657	$4f_{SIN}$
×8 Interpolation	−0.0413	$8f_{SIN}$

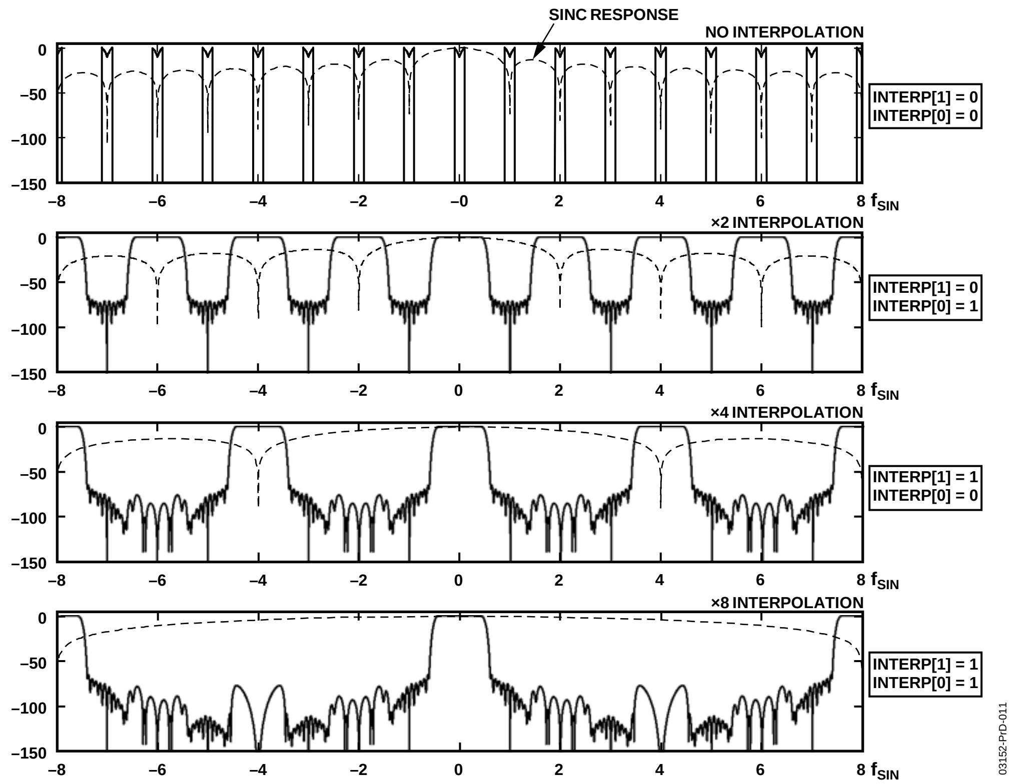
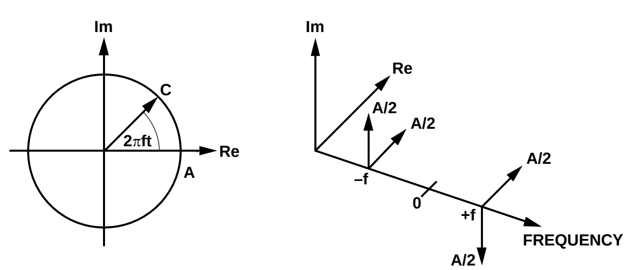


Figure 57. Interpolation Modes

REAL AND COMPLEX SIGNALS

A complex signal contains both magnitude and phase information. Given two signals at the same frequency, if a point in time can be taken such that the signal leading in phase is cosinusoidal and the lagging signal is sinusoidal, then information pertaining to the magnitude and phase of a combination of the two signals can be derived; the combination of the two signals can be considered a complex signal. The cosine and sine can be represented as a series of exponentials; recalling that a multiplication by j is a counterclockwise rotation about the Re/Im plane, the phasor representation of a complex signal, with frequency f, can be shown in Figure 58.



$$C = Ae^{2\pi ft} = A\cos(2\pi ft) + jA\sin(2\pi ft)$$

$$A\cos(2\pi ft) = A\left[\frac{e^{+j2\pi ft} + e^{-j2\pi ft}}{2}\right] = \frac{A}{2}\left[e^{+j2\pi ft} + e^{-j2\pi ft}\right]$$

$$A\sin(2\pi ft) = A\left[\frac{e^{+j2\pi ft} + e^{-j2\pi ft}}{2j}\right] = \frac{A}{2}\left[je^{+j2\pi ft} + e^{-j2\pi ft}\right]$$

Figure 58. Complex Phasor Representation

The cosine term represents a signal on the real plane with mirror symmetry about dc; this is referred to as the real, in-phase or I component of a complex signal. The sine term represents a signal on the imaginary plane with mirror asymmetry about dc; this term is referred to as the imaginary, quadrature or Q complex signal component.

The AD9786 has two channels of interpolation filters, allowing both I and Q components to be shaped by the same filter transfer function. The interpolation filters' frequency response is a real transfer function. Two DACs are required to represent a complex signal. A single DAC can only synthesize a real signal. When a DAC synthesizes a real signal, negative frequency components fold onto the positive frequency axis. If the input to the DAC is mirror symmetrical about dc, the folded negative frequency components fold directly onto the positive frequency components in phase producing constructive signal summation. If the input to the DAC is not mirror symmetric about dc, negative frequency components may not be in phase with positive frequency components and will cause destructive signal summation. Different applications may or may not benefit from either type of signal summation.

MODULATION MODES

Table 30. Single Channel Modulation

MODDUAL	CHANNEL	MOD[1]	MOD[0]	Mode
0	0	0	0	I Channel, no modulation
0	0	0	1	I Channel, modulation by $f_{DAC}/2$
0	0	1	0	I Channel, modulation by $f_{DAC}/4$
0	0	1	1	I Channel, modulation by $f_{DAC}/8$
0	1	0	0	Q Channel, no modulation
0	1	0	1	Q Channel, modulation by $f_{DAC}/2$
0	1	1	0	Q Channel, modulation by $f_{DAC}/4$
0	1	1	1	Q Channel, modulation by $f_{DAC}/8$

Either channel of the AD9786's interpolation filter channels can be routed to the DAC and modulated. In single channel operation the input data may be modulated by a real sinusoid; the input data and the modulating sinusoid will contain both positive and negative frequency components. A double side-band output results when modulating two real signals. At the DAC output the positive and negative frequency components will add in phase resulting in constructive signal summation.

As the modulating sinusoidal frequency becomes a larger fraction of the DAC update rate, f_{DAC}, the more the sinc function of the DAC shapes the modulated signal bandwidth, and the closer the first image moves. As the AD9786 interpolation filter's pass band represents a large portion of the input data's Nyquist band, under certain modulation and interpolation modes it is possible for modulated signal bands to touch or overlap images if sufficient interpolation is not used.

Figure 59 shows the effects of $f_{DAC}/8$ modulation when using 8× interpolation.

Figure 60 to Figure 62 show the effects of real modulation under all interpolation modes. The sinc shaping at the corners of the modulated signal band, and the bandwidth to the first image for those cases whose pass bands do not touch or overlap, are tabulated.

Table 31. Synthesis Bandwidth vs. Interpolation Modes

	Interpolation			
Modulation	**None**	**×2**	**×4**	**×8**
none	f_{SIN}	2 f_{SIN}	4 f_{SIN}	8 f_{SIN}
$f_{DAC}/2$	f_{SIN}	2 f_{SIN}	4 f_{SIN}	8 f_{SIN}
$f_{DAC}/4$	Overlap	Touching	2 f_{SIN}	4 f_{SIN}
$f_{DAC}/8$	Overlap	Overlap	Touching	6 f_{SIN}

Table 32. Modulated Pass-Band Edges Sinc Shaping (Lower/Upper)

	Interpolation			
Modulation	**None**	**×2**	**×4**	**×8**
None	0 −2.8241	0 −0.6708	0 −0.1657	0 −0.0413
$f_{DAC}/2$	−0.0701 −22.5378	−1.1932 −9.1824	−2.3248 −6.1190	−3.0590 −4.9337
$f_{DAC}/4$	Overlap	Touching	−0.2921 −1.9096	−0.5974 −1.3607
$f_{DAC}/8$	Overlap	Overlap	Touching	−0.0727 −0.4614

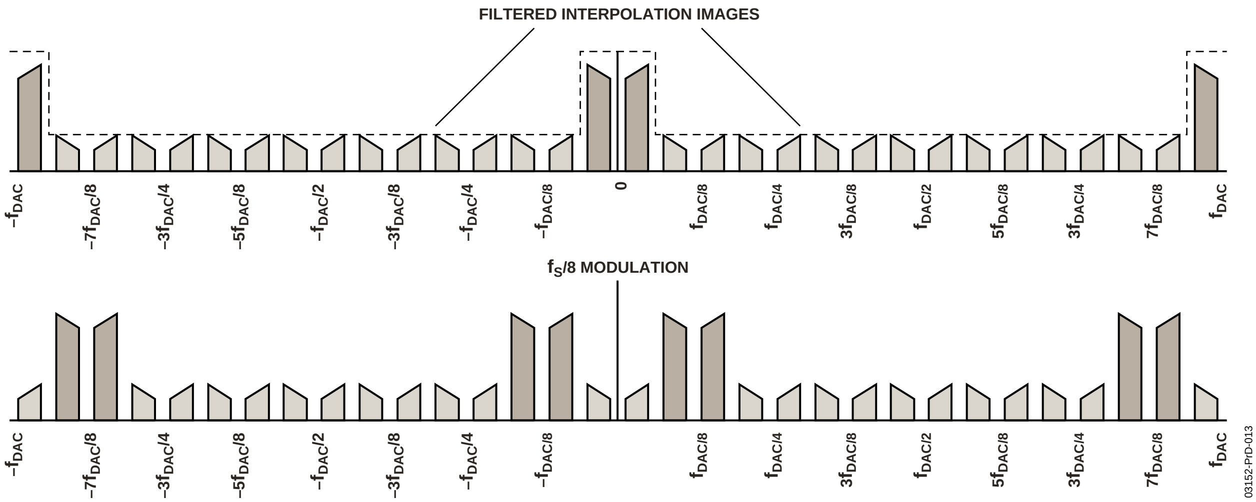


Figure 59. Double Sideband Modulation

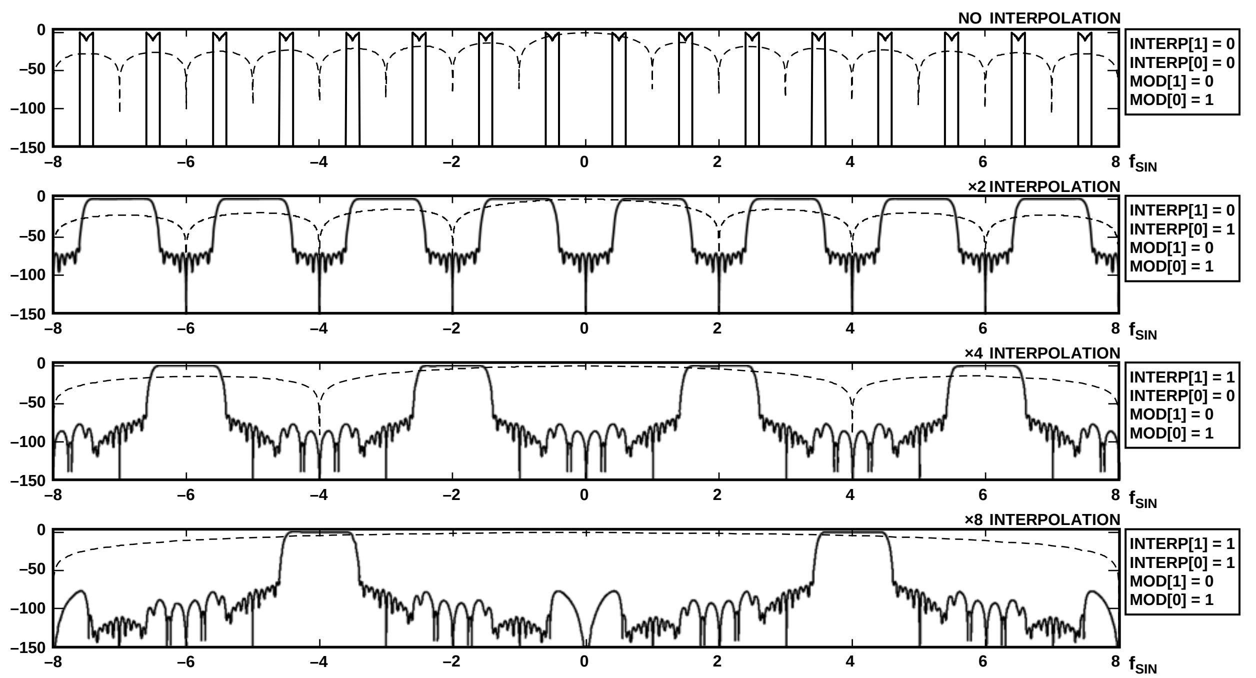


Figure 60. Real Modulation by $f_{DAC}/2$ Under All Interpolation Modes

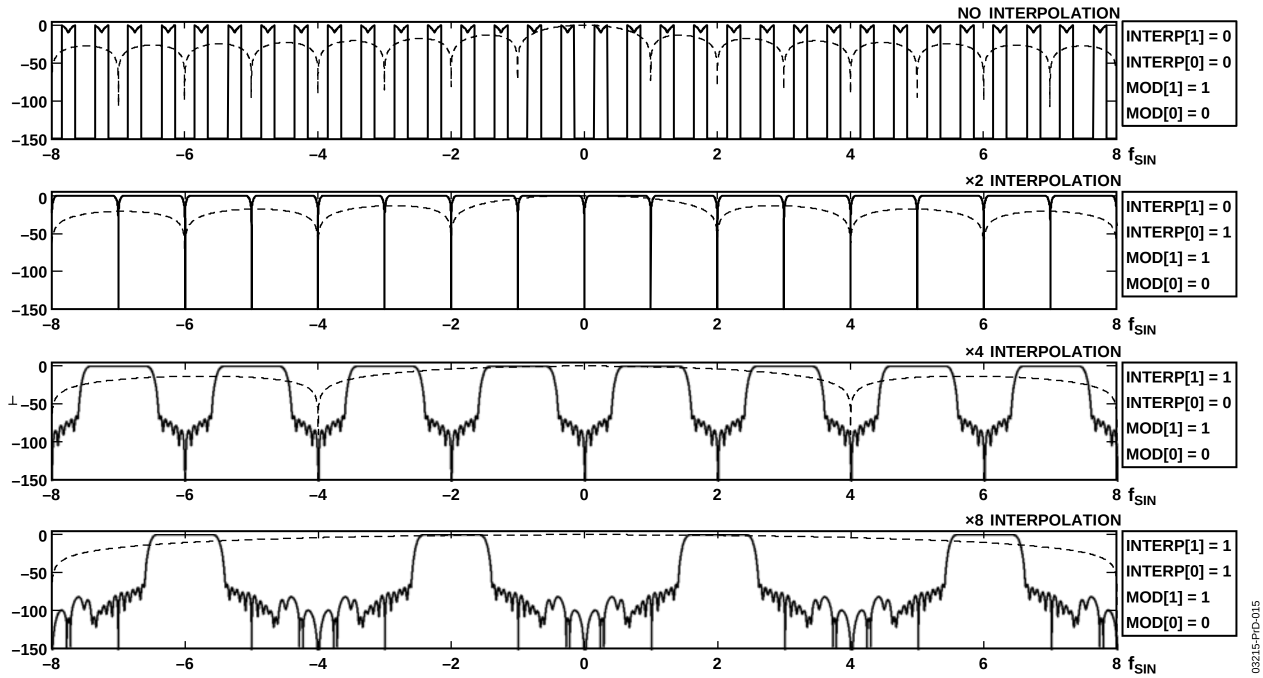


Figure 61. Real Modulation by f_{DAC}/4 Under All Interpolation Modes

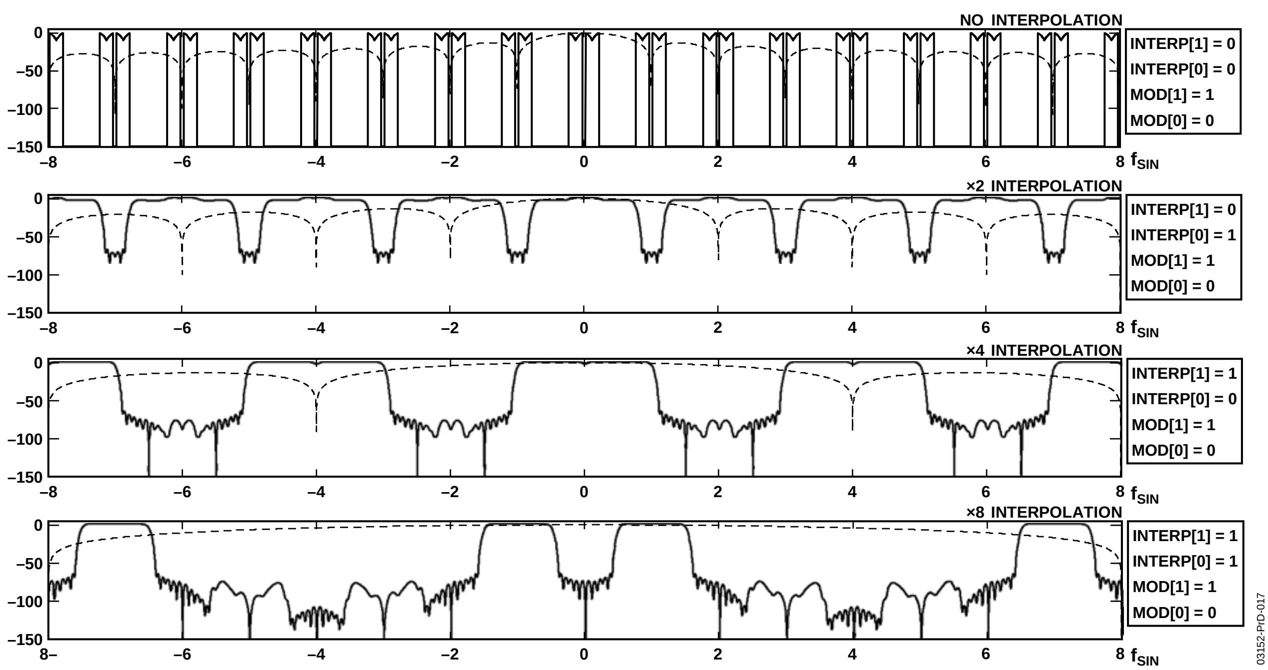


Figure 62. Real Modulation by f_{DAC}/8 Under All Interpolation Modes

Table 33. Dual Channel Complex Modulation

MODSING	REALIMAG	MOD[1]	MOD[0]	Mode
0	0	0	0	Real output, no modulation
0	0	0	1	Real output, modulation by $f_{DAC}/2$
0	0	1	0	Real output, modulation $f_{DAC}/4$
0	0	1	1	Real output, modulation $f_{DAC}/8$
0	1	0	0	Image output, no modulation
0	1	0	1	Image output, modulation by $f_{DAC}/2$
0	1	1	0	Image output, modulation by $f_{DAC}/4$
0	1	1	1	Image output, modulation by $f_{DAC}/8$

In dual channel mode, the two channels may be modulated by a complex signal, with either the real or imaginary modulation result directed to the DAC. Assume initially, as in Figure 63, that the complex modulating signal is defined for a positive frequency only. This causes the output spectrum to be translated in frequency by the modulation factor only. No additional sidebands are created as a result of the modulation process, and therefore the bandwidth to the first image from the baseband bandwidth is the same as the output of the interpolation filters. Furthermore, pass bands will not overlap or touch. The sinc shaping at the corners of the modulated signal band are tabulated in Table 34. Figure 64, Figure 65, and Figure 66 show the effects of complex modulation with varying interpolation rates.

Table 34. Complex Modulated Pass-Band Edges Sinc Shaping (Lower/Upper)

	Interpolation			
Modulation	**None**	**×2**	**×4**	**×8**
None	0	0	0	0
	–2.8241	–0.6708	–0.1657	–0.0413
$f_{DAC}/2$	–0.0701	–1.1932	–2.3248	–3.0590
	–22.5378	–9.1824	–6.1190	–4.9337
$f_{DAC}/4$	–0.4680	–0.0175	–0.2921	–0.5974
	–6.0630	–3.3447	–1.9096	–1.3607
$f_{DAC}/8$	–1.3723	–0.1160	–0.0044	–0.0727
	–4.9592	–1.7195	–0.7866	–0.4614

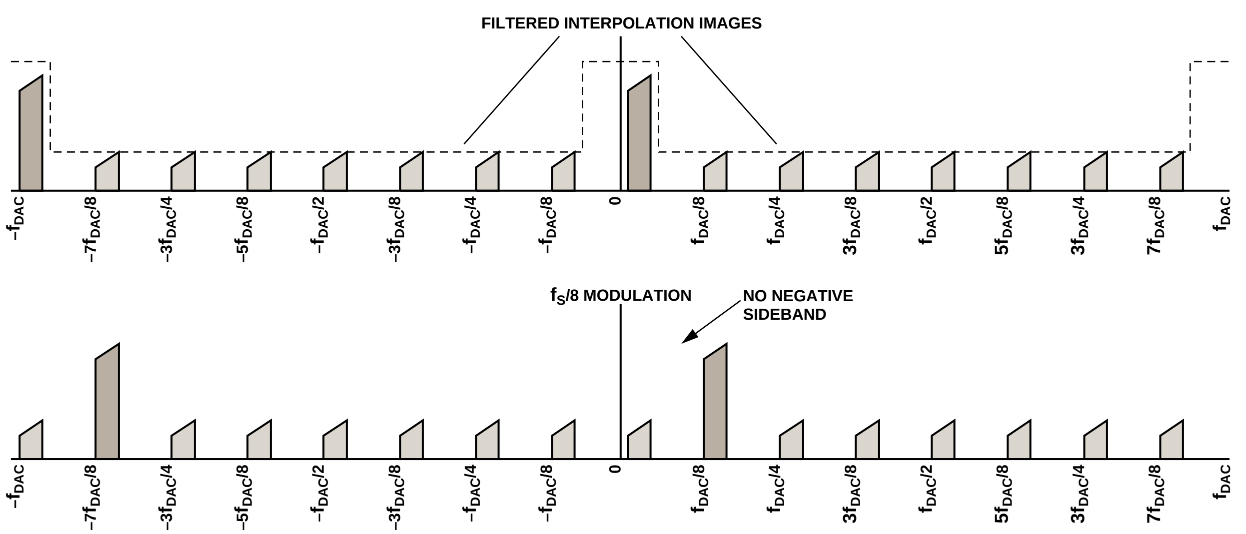


Figure 63. Complex Modulation

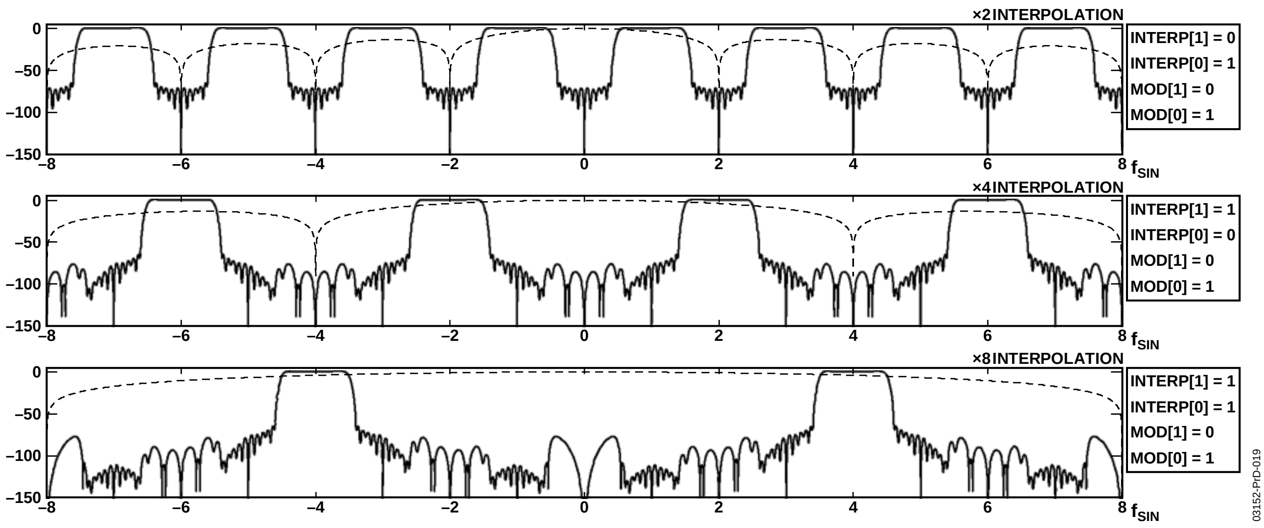


Figure 64. Complex Modulation by $f_{DAC}/2$ Under All Interpolation Modes

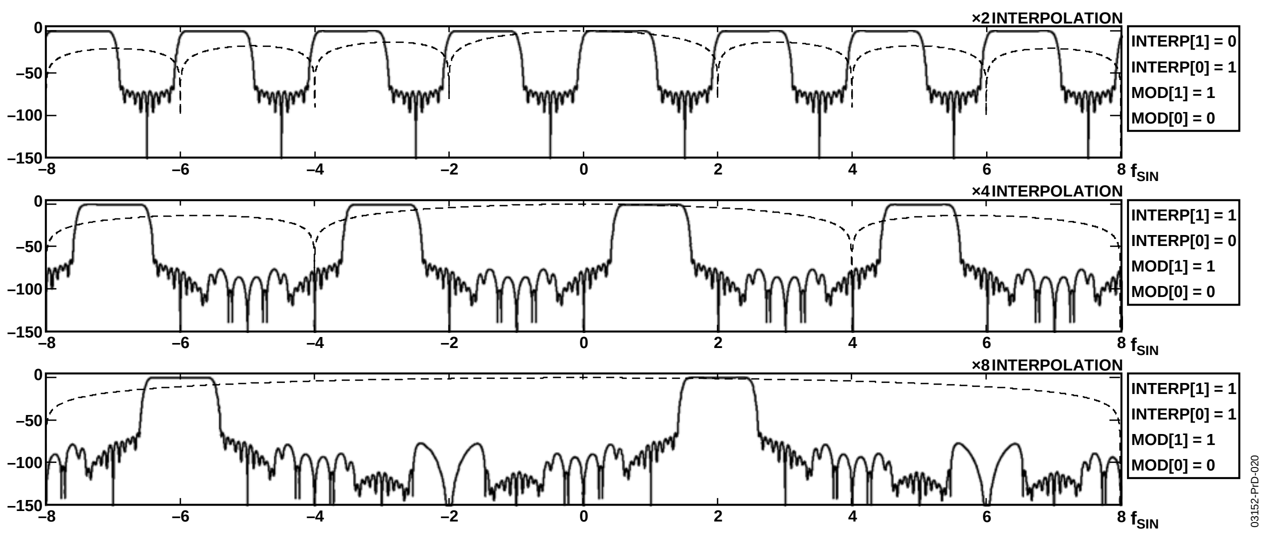


Figure 65. Complex Modulation by $f_{DAC}/4$ Under All Interpolation Modes

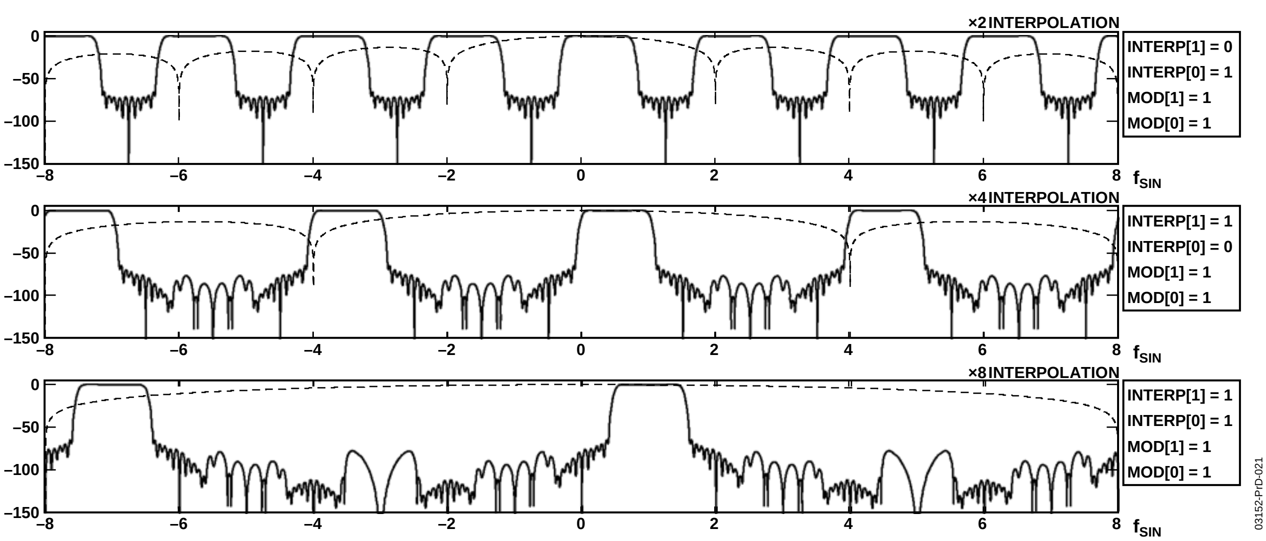


Figure 66. Complex Modulation by $f_{DAC}/8$ Under All Interpolation Modes

POWER DISSIPATION

The AD9786 has seven power supply domains: two 3.3 V analog domains (AVDD1 and AVDD2), two 2.5 V analog domains (ADVDD and ACVDD), one 2.5 V clock domain (CLKVDD), and two digital domains (DVDD, which runs from 2.5 V, and DRVDD, which can run from 2.5 V or 3.3 V).

The current needed for the 3.3 V analog supplies, AVDD1 and AVDD2, is consistent across speed and varying modes of the AD9786. **Nominally, the current for AVDD1 is 29 mA across all speeds and modes, while the current for AVDD2 is 20 mA.**

The current for the 2.5 V analog supplies and the digital supplies varies depending on speed and mode of operation. Figure 67, Figure 68, and Figure 69 show this variation. Note that CLKVDD, ADVDD, and ACVDD vary with clock speed and interpolation rate, but not with modulation rate.

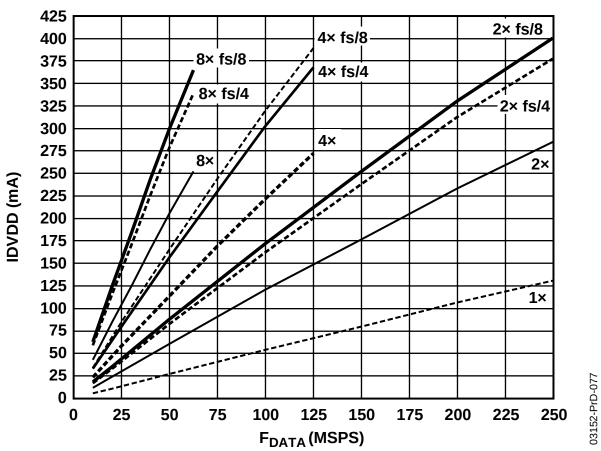


Figure 67. DVDD Supply Current vs. Clock Speed, Interpolation, and Modulation Rates

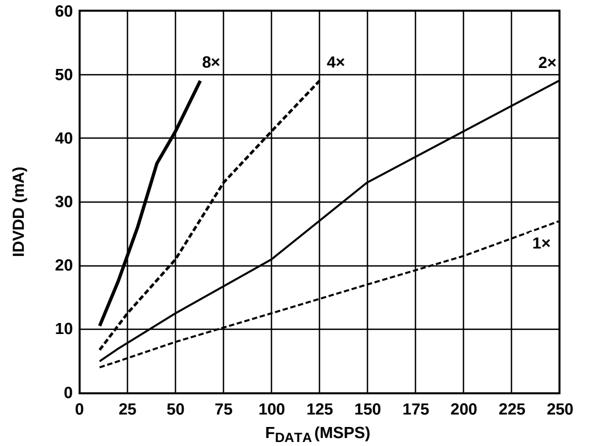


Figure 68. CLKVDD Supply Current vs. Clock Speed and Interpolation Rates

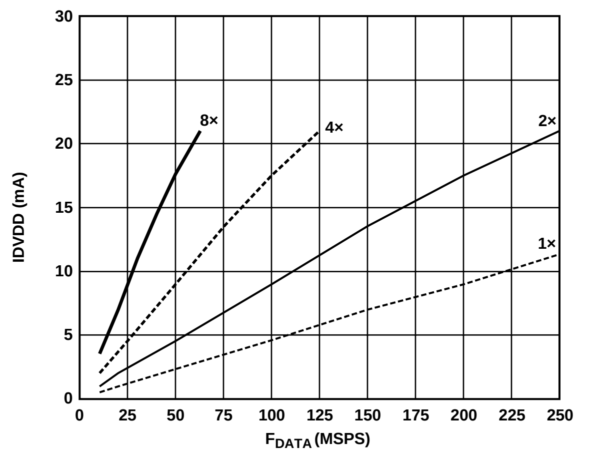


Figure 69. ADVDD and ACVDD Supply Current vs. Clock Speed and Interpolation Rates

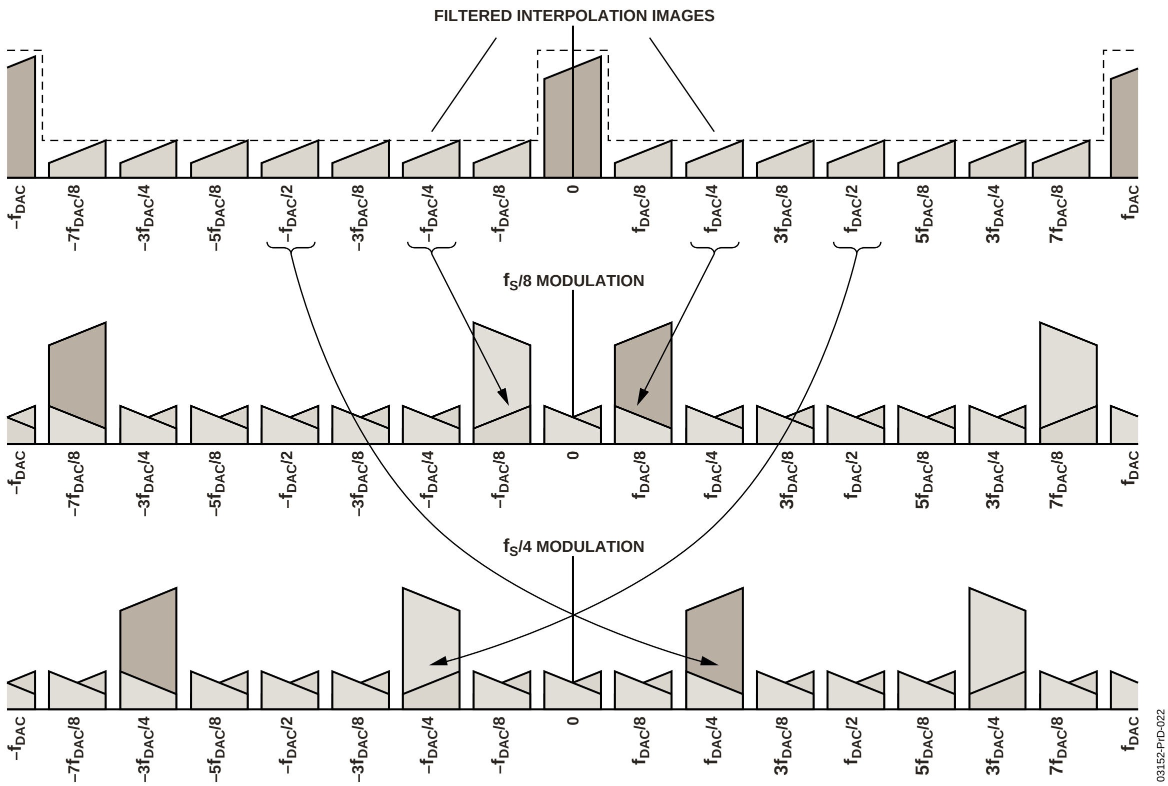


Figure 70. Complex Modulation with Negative Frequency Aliasing

Table 35. Dual Channel Complex Modulation with Hilbert

Hilbert	Mode
0	Hilbert transform off
1	Hilbert transform on

When complex modulation is performed, the entire spectrum is translated by the modulation factor. If the resulting modulated spectrum is not mirror symmetric about dc, when the DAC synthesizes the modulated signal, negative frequency components will fall on the positive frequency axis and can cause destructive summation of the signals, as shown in Figure 70. For some applications, this can distort the modulated output signal.

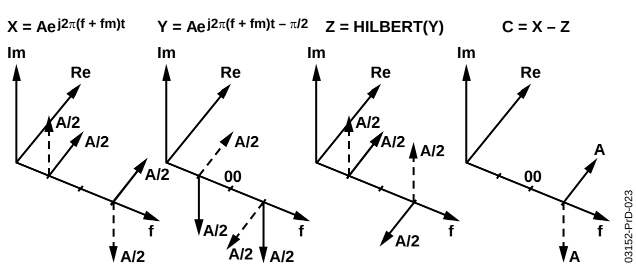


Figure 71. Negative Frequency Image Rejection

Referring to Figure 71, by performing a second complex modulation with a modulating signal having a fixed π/2 phase difference, Figure (Y), relative to the original complex modulation signal, Figure (X), taking the Hilbert transform of the new resulting complex modulation, and subtracting it from the original complex modulation output all negative frequency components can be folded in phase to the positive frequency axis before being synthesized by the DAC. When the DAC synthesizes the modulated output there are no negative frequency components to fold onto the positive frequency axis out of phase; consequently no distortion is produced as a result of the modulation process.

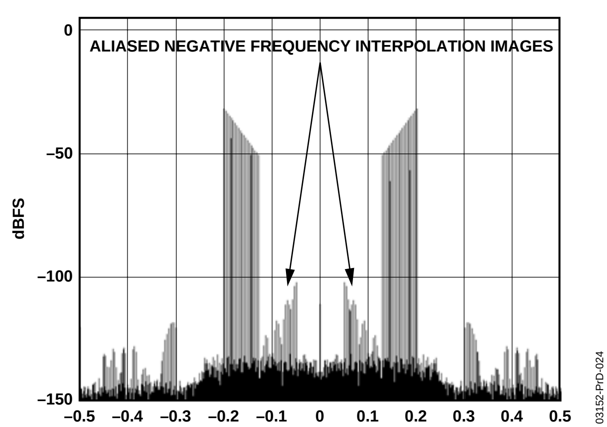


Figure 72. Negative Frequency Aliasing Distortion

Figure 72 shows this effect at the DAC output for a mirror asymmetric signal about dc produced by complex modulation without a Hilbert transform. The signal bandwidth was narrowed to show the aliased negative frequency interpolation images.

In contrast, Figure 73 shows the same waveform with the Hilbert transform applied. Clearly, the aliased interpolation images are not present.

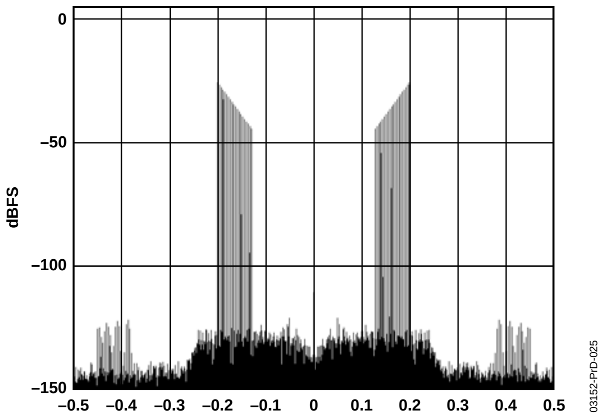


Figure 73. Effects of Hilbert Transform

If the output of the AD9786 is to be used with a quadrature modulator, negative frequency images are cancelled without the need of a Hilbert transform.

HILBERT TRANSFORM IMPLEMENTATION

The Hilbert transform on the AD9786 is implemented as a 19-coefficient FIR. The coefficients are given in Table 36.

Table 36.

Coefficient	Integer Value
H(1)	–6
H(2)	0
H(3)	–17
H(4)	0
H(5)	–40
H(6)	0
H(7)	–91
H(8)	0
H(9)	–318
H(10)	0
H(11)	318
H(12)	0
H(13)	91
H(14)	0
H(15)	40
H(16)	0
H(17)	17
H(18)	0
H(19)	6

The transfer function of an ideal Hilbert transform has a +90° phase shift for negative frequencies, and a –90° phase shift for positive frequencies. Because of the discontinuities that occur at 0 Hz and at 0.5 × Sample Rate, any real implementation of the Hilbert Transform trades off bandwidth versus ripple.

Figure 74 and Figure 75 show the gain of the Hilbert transform versus frequency. Gain is essentially flat, with a pass-band ripple of 0.1 dB over the frequency range 0.07 × Sample Rate to 0.43 × Sample Rate.

Figure 76 shows the phase response of the Hilbert transform implemented in the AD9786. The phase response for positive frequencies begins at –90° at 0 Hz, followed by a linear phase response (pure time delay) equal to nine filter taps (nine DACCLK cycles). For negative frequencies, the phase response at 0 Hz is +90°, again followed by a linear phase delay of nine filter taps. To compensate for the unwanted 9-cycle delay, an equal delay of nine taps is used in the AD9786 digital signal path opposite to the Hilbert transform. This delay block is noted as t on the block diagram on the first page of this data sheet.

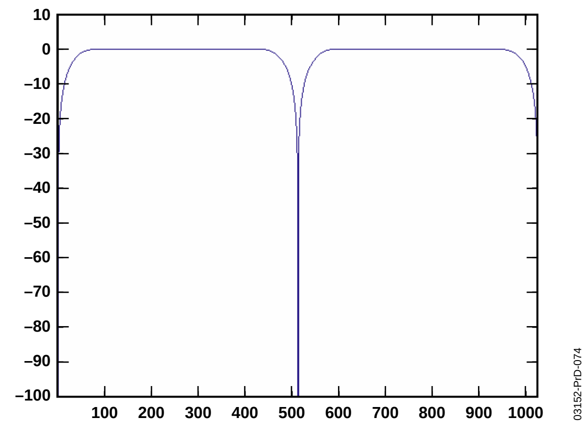


Figure 74. Hilbert Transform Gain

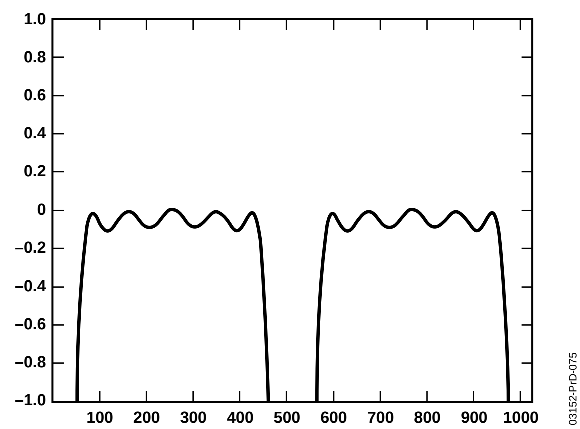


Figure 75. Hilbert Transform Ripple

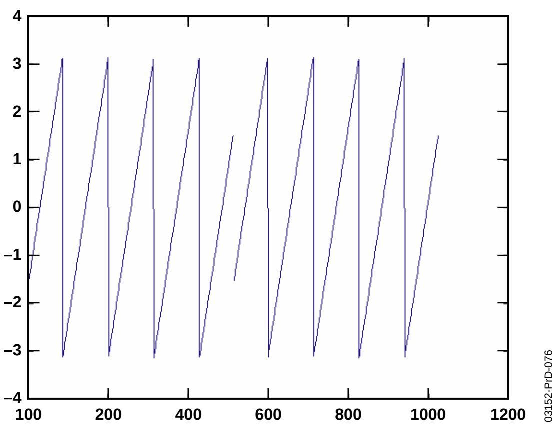


Figure 76. Phase Response of Hilbert Transform

Table 37. Dual Channel Complex Modulation Sideband Selection

Sideband	Mode
0	Lower IF sideband rejected
1	Upper IF sideband rejected

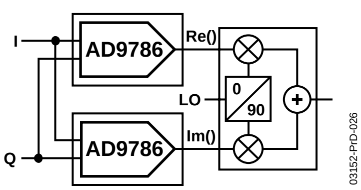


Figure 77. AD9786 Driving Quadrature Modulator

The AD9786 can be configured to drive a quadrature modulator representatively, as in Figure 77. Where two AD9786s are used with one AD9786 producing the real output, the second AD9786 produces the imaginary output. By configuring the AD9786 as a complex modulator coupled to a quadrature modulator, IF image rejection is possible. The quadrature modulator acts as the real part of a complex modulation producing a double sideband spectrum at the local oscillator (LO) frequency, with mirror symmetry about dc.

A baseband double sideband signal modulated to IF increases IF filter complexity and reduces power efficiency. If the baseband signal is complex, a single sideband IF modulation can be used, relaxing IF filter complexity and increasing power efficiency.

The AD9786 has the ability to place the baseband single sideband complex signal either above the IF frequency or below it. Figure 78, Figure 79, and Figure 80 illustrate this.

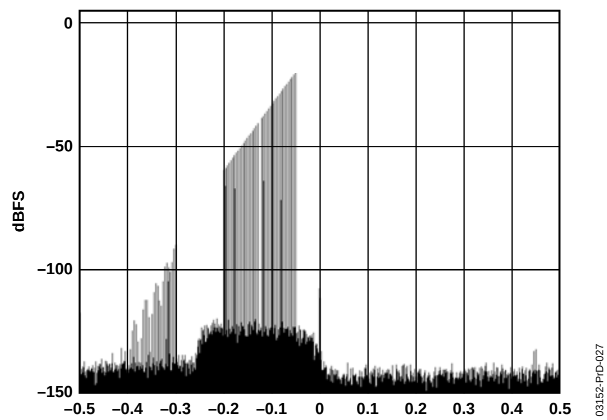


Figure 78. Upper IF Sideband Rejected

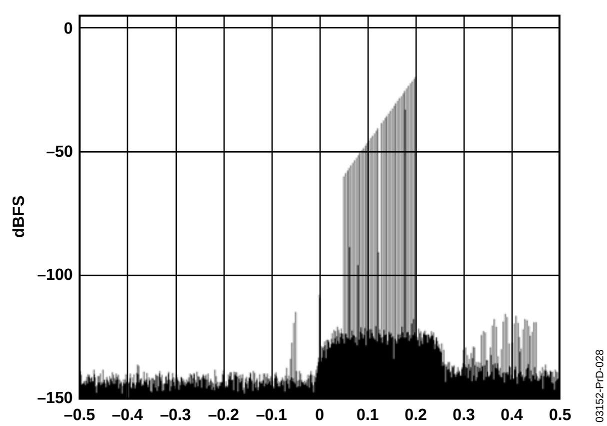


Figure 79. Lower IF Sideband Rejected

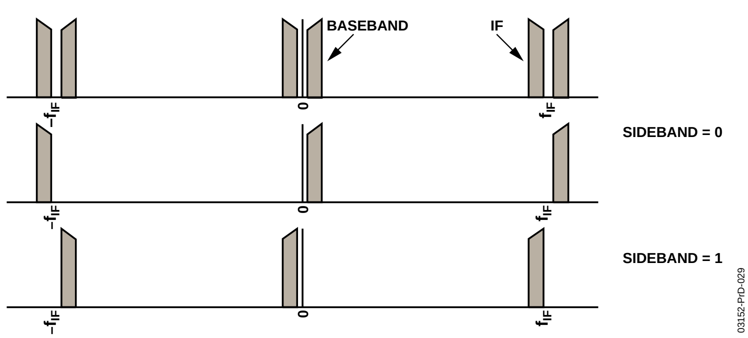


Figure 80. IF Quadrature Modulation of Real and Complex Baseband Signals

Master/Slave, Modulator/DATACLK Master Modes

In applications where two or more AD9786s are used to synthesize several digital data paths, it may be necessary to ensure that the digital inputs to each device are latched synchronously. In complex data processing applications, digital modulator phase alignment may be required between two AD9786s. In order to allow data synchronization and phase alignment, only one AD9786 should be configured as a master device, providing a reference clock for another slave-configured AD9786.

With synchronization enabled, a reference clock signal is generated on the DATACLK pin of the master. The DATACLK pins on the slave devices act as inputs for the reference clock generated by the master. The DATACLK pin on the master and all slaves must be directly connected. All master and slave devices must have the same clock source connected to their respective CLK+/CLK– pins.

When configured as a master, the reference clock generated may take one of two forms. In modulator master mode, the reference clock will be a square wave with a period equal to 16 cycles of the DAC update clock. Internal to the AD9786 is a 16-state finite state machine, running at the DAC update rate. This state machine generates all internal and external synchronization clocks and modulator phasings. The rising edge of the master reference clock is time aligned to the internal state machine's state zero. Slave devices use the master's reference clock to synchronize their data latching and align their modulator's phase by aligning their local state machine state zero to the master.

The second master mode, DATACLK master mode, generates a reference clock that is at the channel data rate. In this mode, the slave devices align their internal channel data rate clock to the master. If modulator phase alignment is needed, a concurrent serial write to all slave devices is necessary. To achieve this, the CSB pin on all slaves must be connected together and a group serial write to the MODADJ register bits must be performed; the modulator coefficient alignment is updated on the next rising edge of the internal state machine following a successful serial write, see Figure 81. Modulator master mode does not need a concurrent serial write as slaves lock to the master phase automatically.

In a slave device, the local channel data rate clock and the digital modulator clock are created from the internal state machine. The local channel data rate clock is used by the slave to latch digital input data. At high data rates, the delay inherent in the signal path from master to slave may cause the slave to lag the master when acquiring synchronization. To account for this, an integer number of the DAC update clock cycles may be programmed into the slave device as an offset. The value in DATADJ allows the local channel data rate clock in the slave device to advance by up to eight cycles of the DAC clock or to be delayed by up to seven cycles, see Figure 84.

The digital modulator coefficients are updated at the DAC clock rate and decoded in sequential order from the state machine according to Figure 83. The MODADJ bits can be used to align a different coefficient to the finite state machine's zero state as shown in Figure 84.

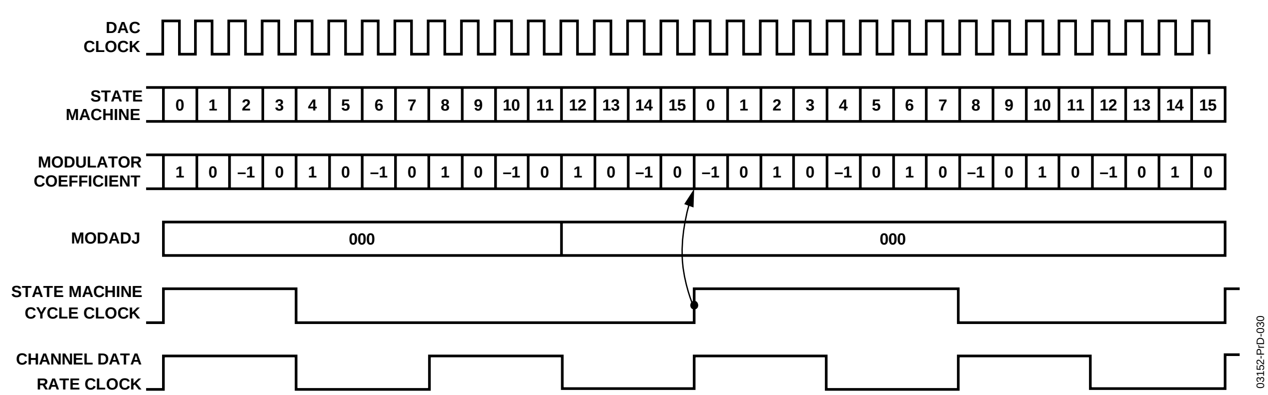


Figure 81. Synchronous Serial Modulator Phase Alignment

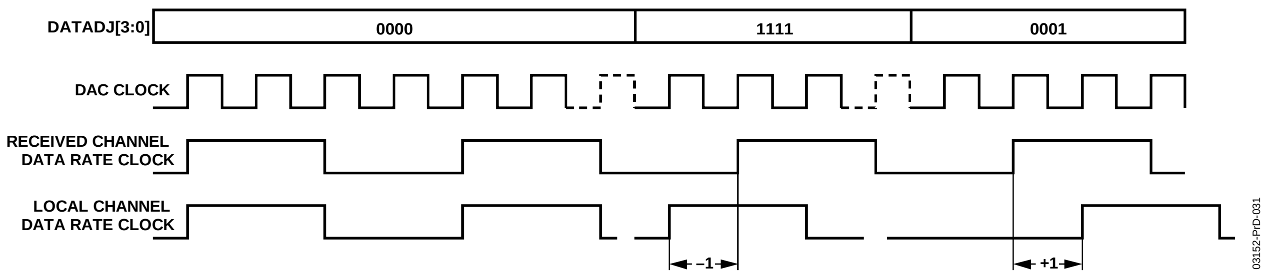


Figure 82. Local Channel Data Rate Clock Synchronized with Offset

STATE	0	1	2	3	4	5	6	7	8	9	10	11	12	13	14	15
DECODE	1	0	$1/\sqrt{2}$	0	0	0	$-1/\sqrt{2}$	0	–1	0	$-1/\sqrt{2}$	0	0	0	$-1/\sqrt{2}$	0
fs/8	0	→	1	→	2	→	3	→	4	→	5	→	6	→	7	→
fs/4	0		→		1		→		2		→		3		→	
fs/2	0				→				1				→			

Figure 83. Digital Modulator State Machine Decode

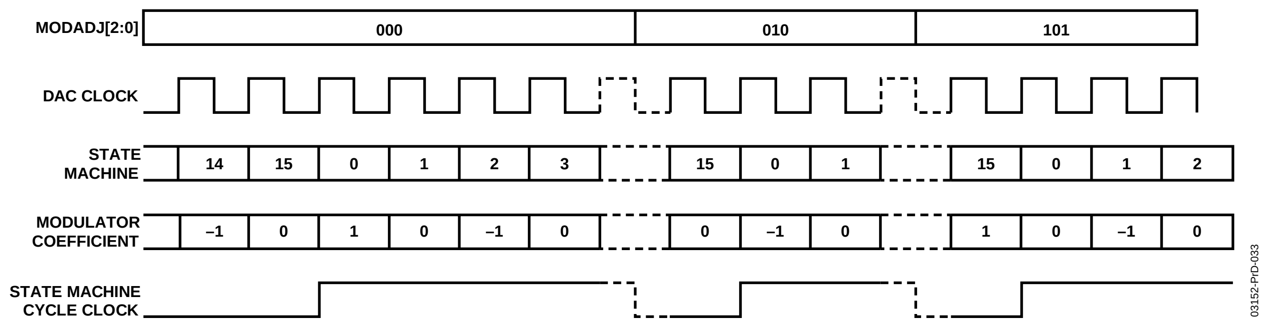


Figure 84. Local Modulator Coefficient Synchronized with Offset

OPERATING THE AD9786 REV F EVALUATION BOARD

This section helps the user get started with the AD9786 evaluation board. Because it is intended to provide starter information to power up the board and verify correct operation, a description of some of the more advanced modes of operation has been omitted.

POWER SUPPLIES

The AD9786 Rev F Evaluation Board has five power supply connectors, labeled AVDD1, AVDD2, (ACVDD, ADVDD), CLKVDD, and DVDD. The AD9786 itself actually has seven power supply domains. To reconcile the power supply domains on the chip with the power supply connectors on the evaluation board, use Table 38.

Additionally, the DRVDD power supply on the AD9786 is used to supply power for the digital input bus. DRVDD can be run from 2.5 V or 3.3 V. On the evaluation board, DRVDD is jumper selectable by JP1, just to the left of the chip on the evaluation board. With the jumper set to the 3.3 V position, DRVDD chip receives its power from VDD3IN. With the jumper set to the 2.5 V position, DRVDD receives its power from AVDIN.

PECL CLOCK DRIVER

The AD9786 system clock is driven from an external source via connector S1. The AD9786 Evaluation Board includes an OnSemiconductor MC100EPT22 PECL clock driver. In the factory, the evaluation board is set to use this PECL driver as a single-ended-to-differential clock receiver. The PECL driver can be set to run from 2.5 V from the CLKVDD power connector, or 3.3 V from the VDD3IN power connector. This setting is done via jumper, JP2, situated next to the CLKVDD power connector, and by setting input bias resistors R23 and R4 on the evaluation board. The factory default is for the PECL driver to be powered from CLKVDD at 2.5 V (R23 = 90.9 Ω, R4 = 115 Ω). To operate the PECL driver with a 3.3 V supply, R23 must be replaced with a 115 Ω resistor and R4 must be replaced with a 90.9 Ω resistor, as well as changing the position of JP2. The schematic of the PECL driver section of the evaluation board is shown in Figure 85. A low jitter sine wave should be used as the clock source. Care must be taken to make sure the clock amplitude does not exceed the power supply rails for the PECL driver.

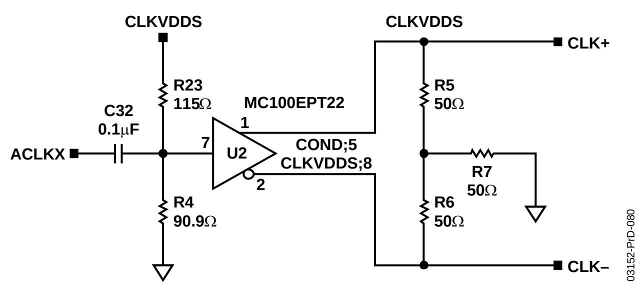


Figure 85. PECL Driver on AD9786 Rev E Evaluation Board

Table 38.

Evaluation Board Label/ PS Domain on Chip	Nominal Power Supply Voltage (V)	Description
DVDD	2.5	SPI port
CLKVDD	2.5	Clock circuitry
(ACVDD ADVDD)	2.5	Analog circuitry containing clock and digital interface circuitry
AVDD2	3.3	Switching analog circuitry
AVDD1	3.3	Analog output circuitry

DATA INPUTS

Digital data inputs to the AD9786 are accessed on the evaluation board through connectors J1 and J2. These are 40 pin right angle connectors that are intended to be used with standard ribbon cable connectors. The input levels should be either 3.3 V or 2.5 V CMOS, depending on the setting of the DRVDD jumper JP1. The data format is selectable through Register 02h, Bit 7 (DATAFMT). With this bit set to a default 0, the AD9786 assumes that the input data is in twos complement format. With this bit set to 1, data should be input in offset binary format.

When the evaluation board is first powered up and the clock and data are running, it is recommended that the proper operating current is verified. Depress reset switch SW1 to ensure that the AD9786 is in the default mode. The default mode for the AD9786 is for the interpolation set to 1×. The modulator is turned off in the default mode. The nominal operating currents for the evaluation board in the power-up default mode are shown in Table 39.

Additionally, the DRVDD power supply on the AD9786 is used to supply power for the digital input bus. DRVDD can be run from 2.5 V or 3.3 V. On the evaluation board, DRVDD is jumper selectable by JP1, just to the left of the chip on the evaluation board. With the jumper set to the 3.3 V position, DRVDD chip receives its power from VDD3IN. With the jumper set to the 2.5 V position, DRVDD receives its power from AVDIN.

SERIAL PORT

SW1 is a hard reset switch that sets the AD9786 to its default state. It should be used every time the AD9786 power supply is cycled or the clock is interrupted, or if new data is to be written via the SPI port. Set the SPI software to read back data from the AD9786 and verify that when the software is run, the expected values are read back.

Table 39. Nominal Operating Currents in Power-Up Default Mode

	Nominal Current @ Speed (mA)			
Evaluation Board Power Supply	**50 MSPS**	**100 MSPS**	**150 MSPS**	**200 MSPS**
DVDD	26	49	74	99
CLKVDD	78	83	87	92
ACVDD and ADVDD	1	4	6	8
AVDD1	30	30	30	30
AVDD2	27	27	27	27

Table 40. SPI Registers

Register	Bit 7	Bit 6	Bit 5	Bit 4	Bit 3	Bit 0
01h	INTERP[1]	INTERP[0]				

ANALOG OUTPUT

The analog output of the AD9786 is accessed via connector S3. Once all settings are selected and current levels and SPI port functionality are verified, the analog signal at S3 can be viewed. For most of the AD9786's applications, a spectrum analyzer is the instrument of choice to verify proper performance. A typical spectral plot is shown in Figure 86, with the AD9786 synthesizing a two-tone signal in the default mode with a 200 MSPS sample rate. A single tone CW signal should provide output power of approximately +0.5 dBm to the spectrum analyzer.

If the spectrum does not look correct at this point, the data input may be violating setup and hold times with respect to the input clock. To correct this, the user should vary the input data timing. If this is not possible, SPI Register 02h, Bit 4 (DCLKPOL) can be inverted. This bit controls the clock edge upon which the data is latched. If these methods do not correct the spectrum, it is unlikely that the issue is timing related. This note should then be reread to verify that all instructions have been followed.

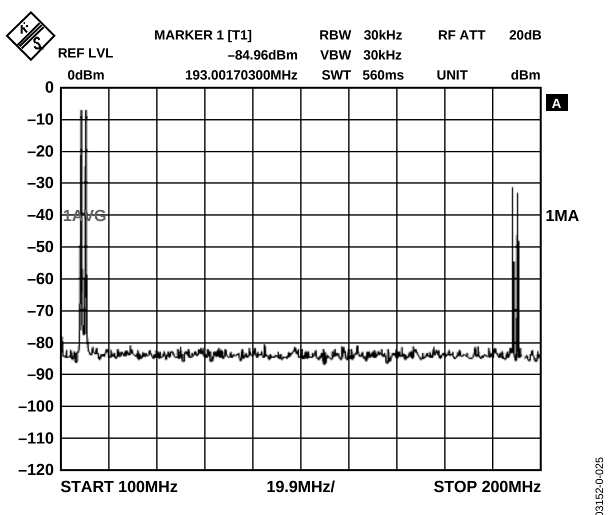


Figure 86. Typical Spectral Plot

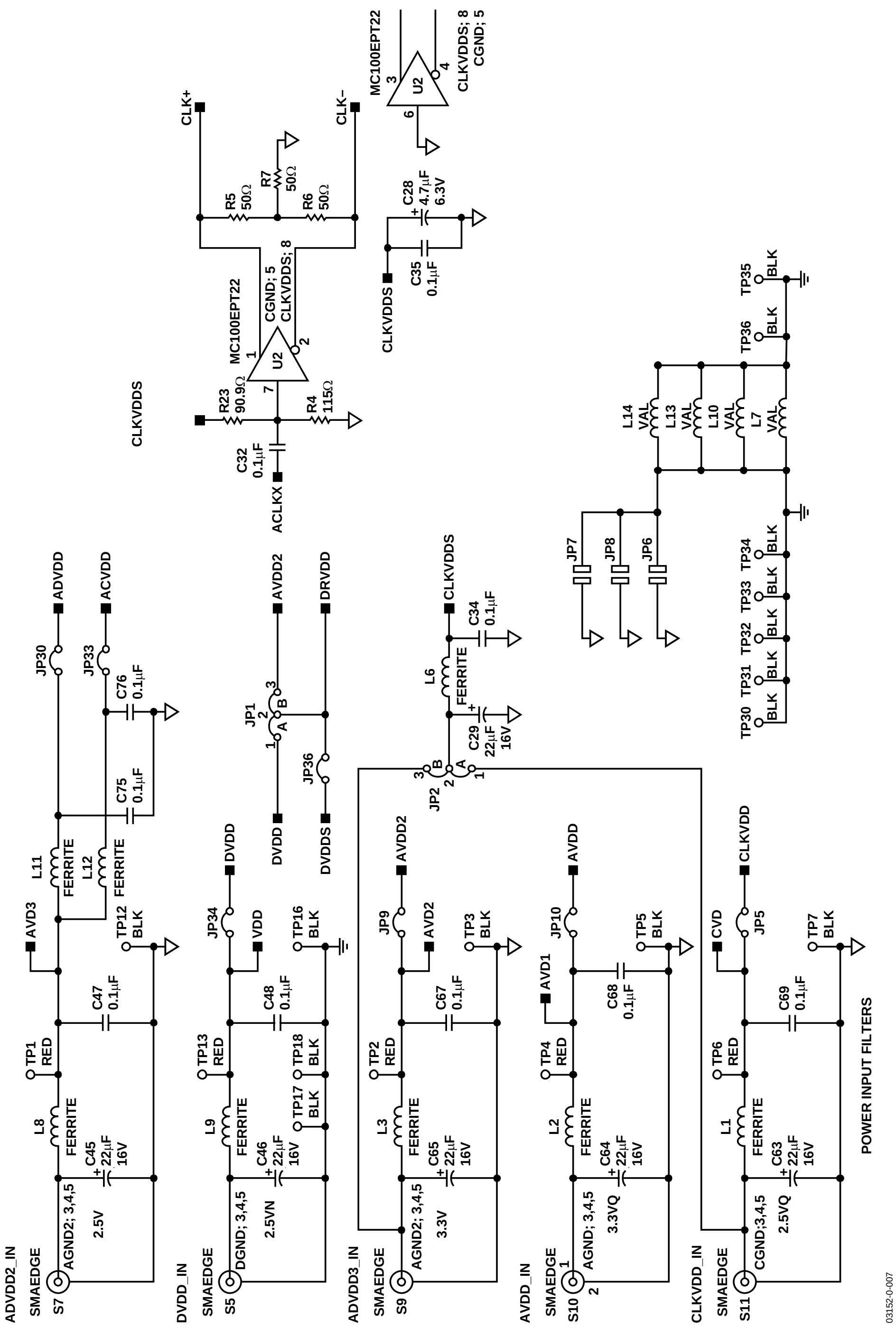


Figure 87. Power Supply Distribution Rev F Evaluation Board

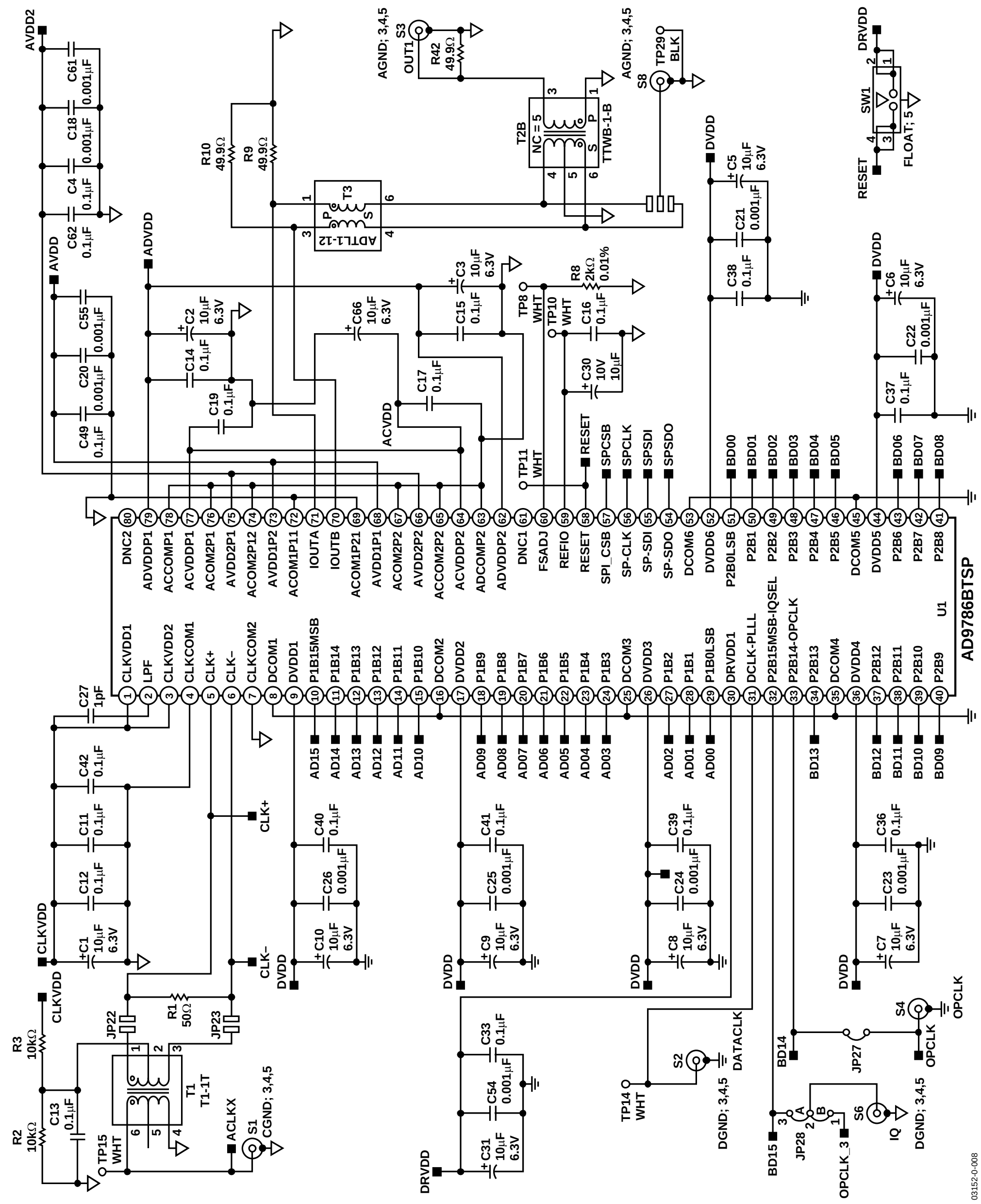


Figure 88. AD9786 Local Circuitry Rev F Evaluation Board

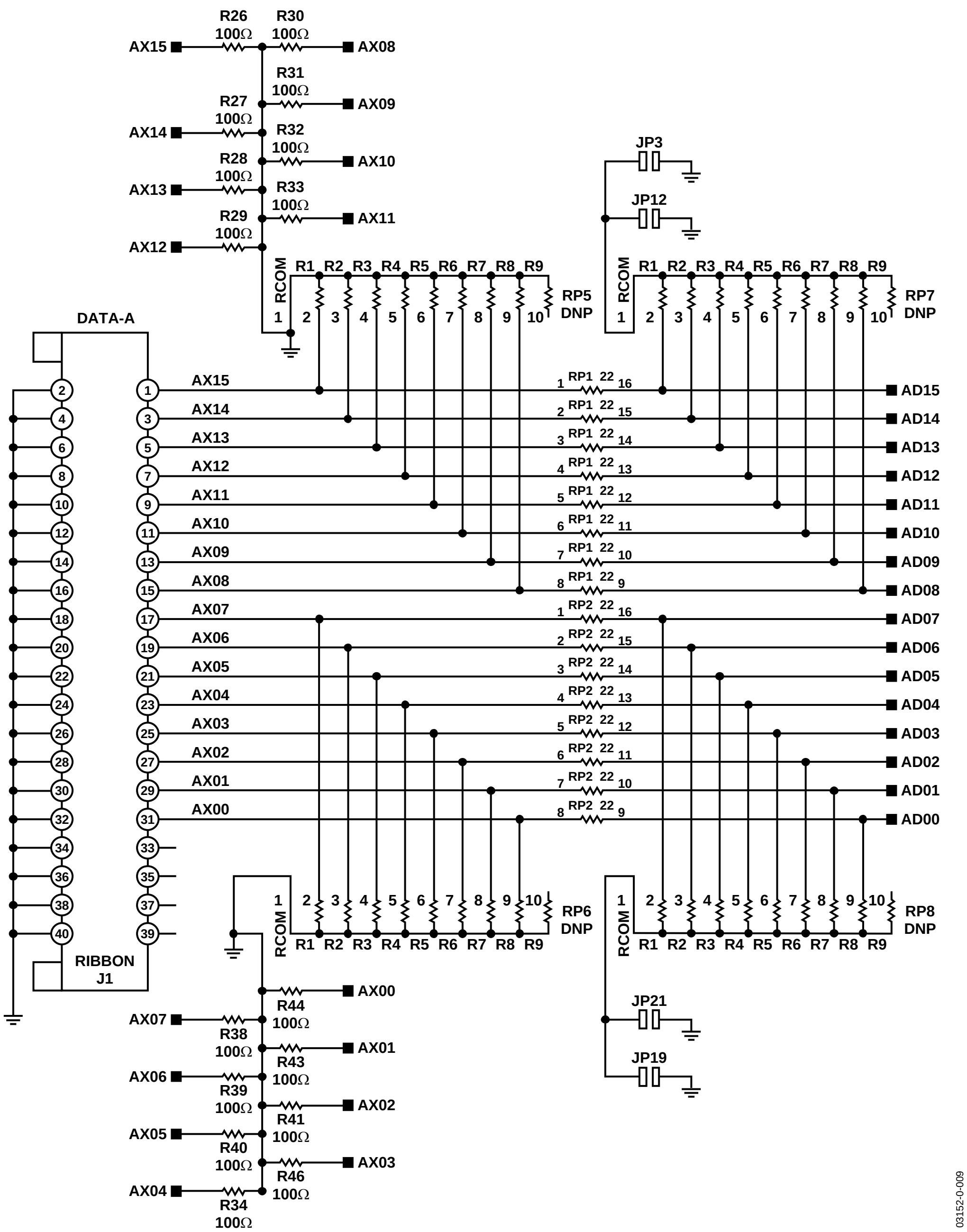


Figure 89. Digital Data Port A Input Terminations Rev F Evaluation Boards

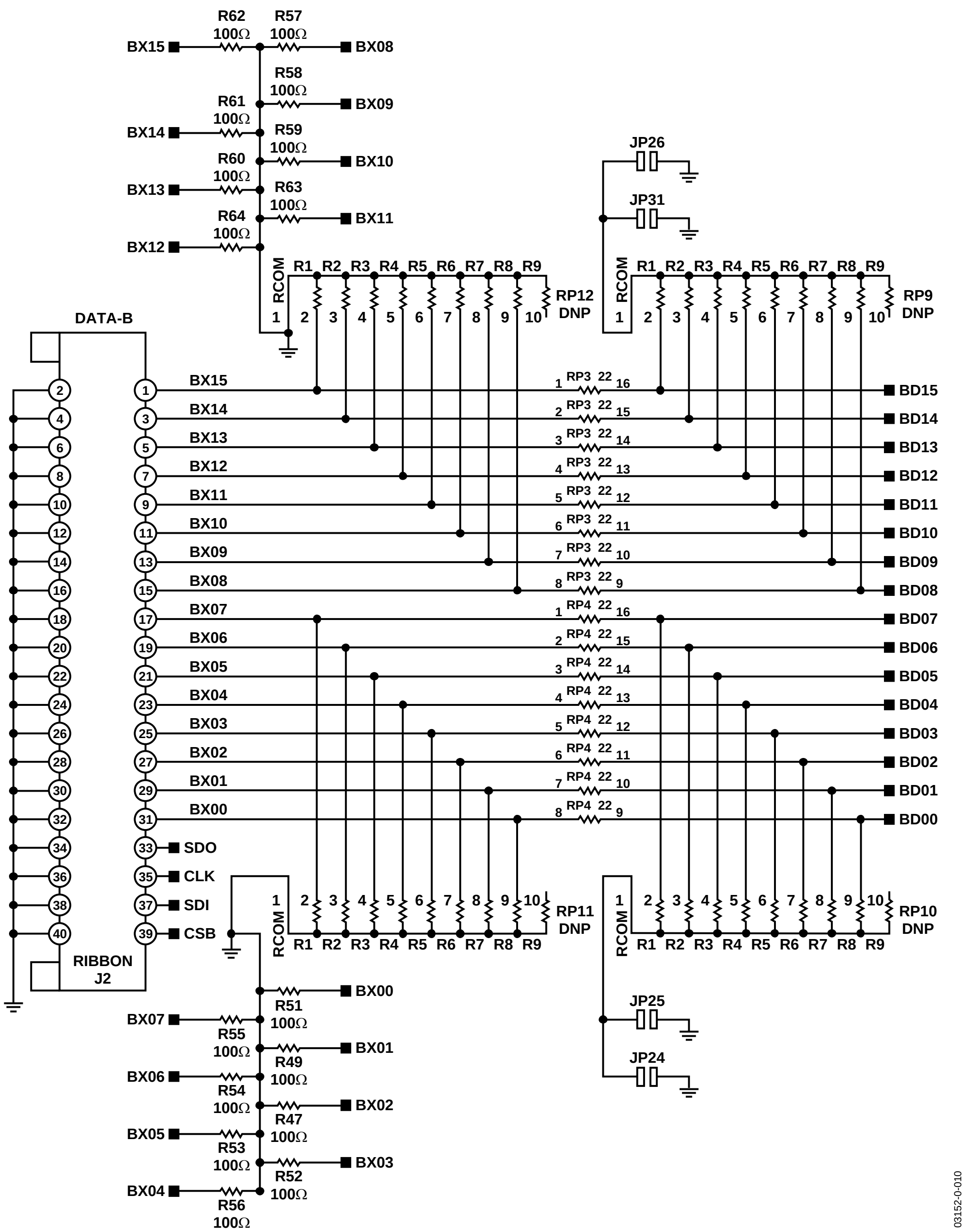


Figure 90. Digital Data Port B Input Terminations Rev F Evaluation Board

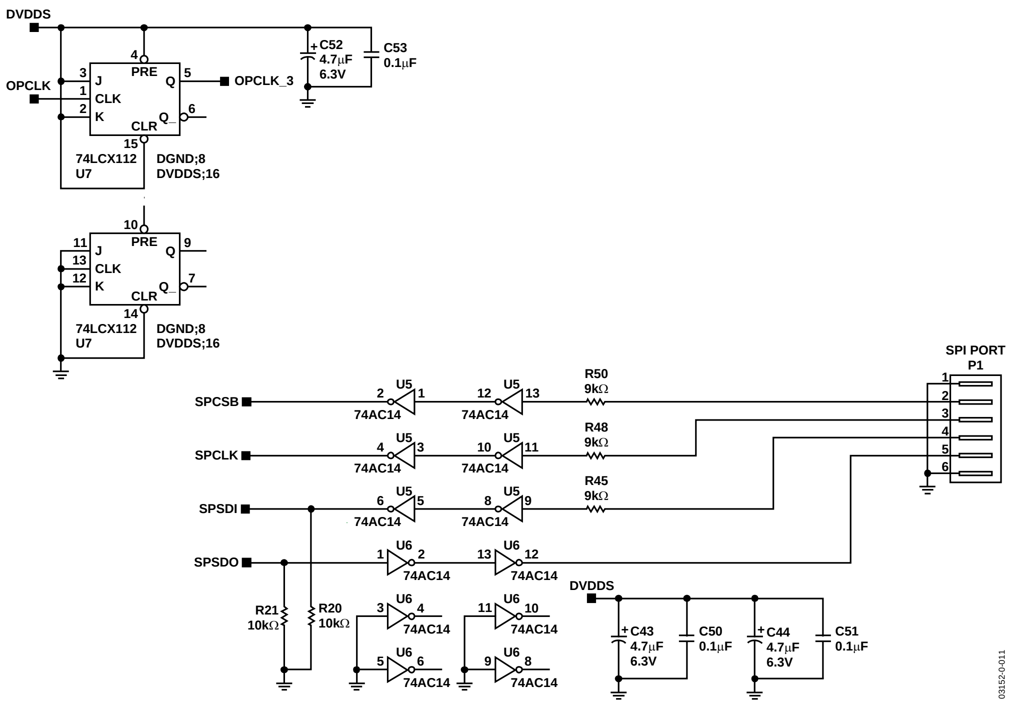


Figure 91. SPI and One-Port Clock Circuitry Rev F Evaluation Board

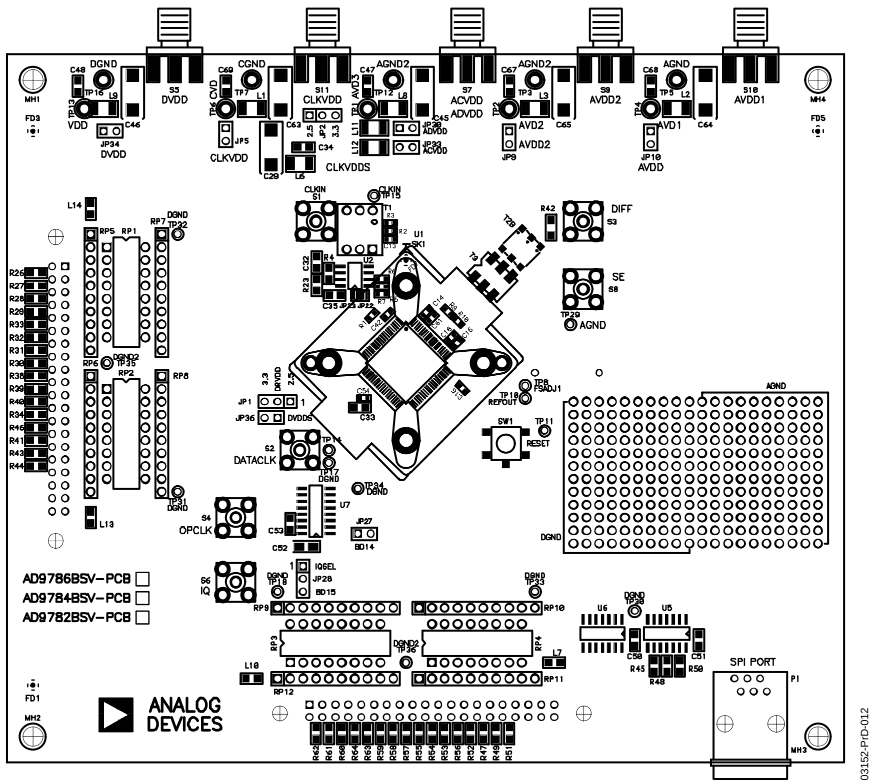


Figure 92. PCB Assembly, Primary Side Rev F Evaluation Board

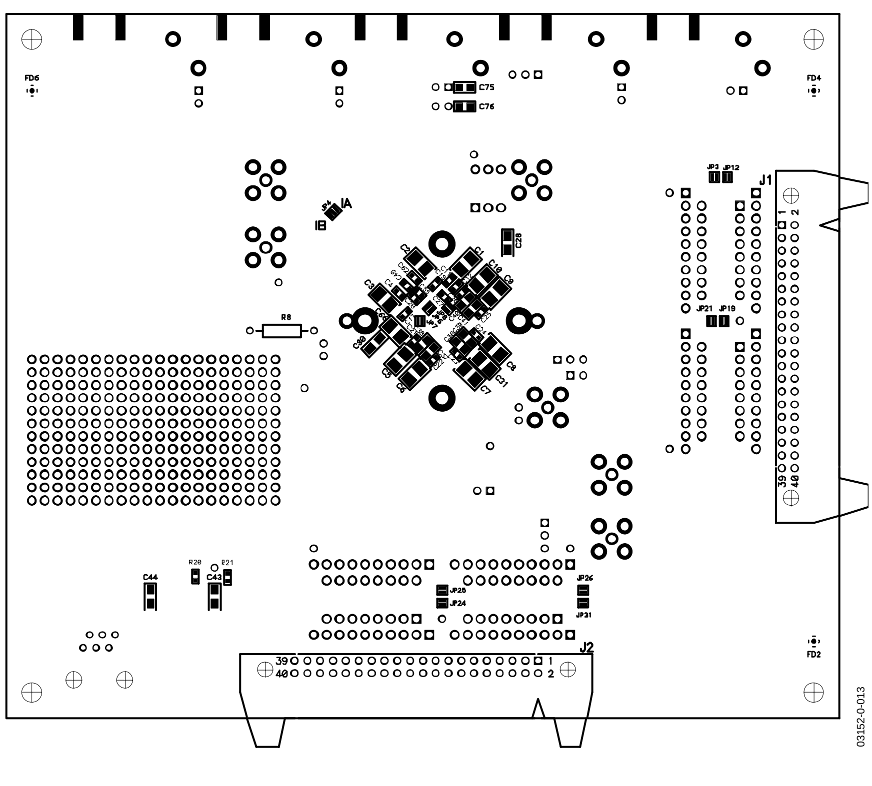


Figure 93. PCB Assembly, Secondary Side Rev F Evaluation Board

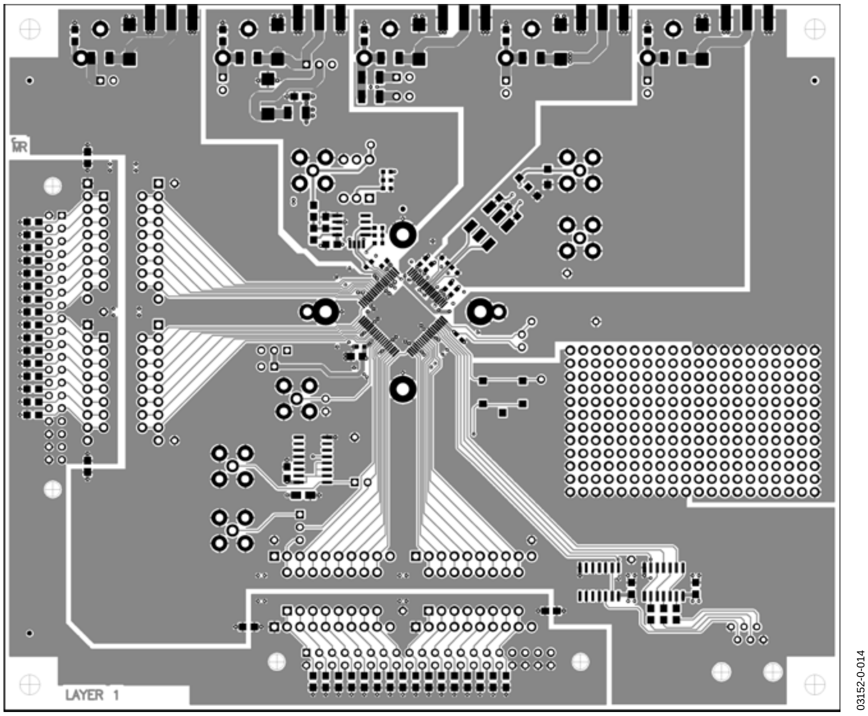


Figure 94. PCB Assembly, Layer 1 Metal Rev F Evaluation Board

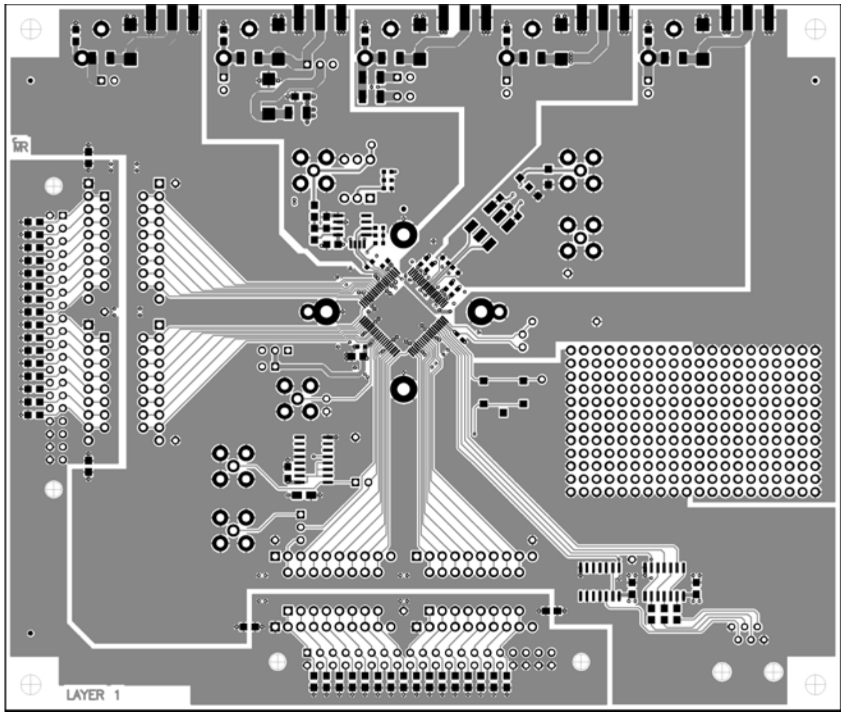


Figure 95. PCB Assembly, Layer 1 Metal Rev F Evaluation Board

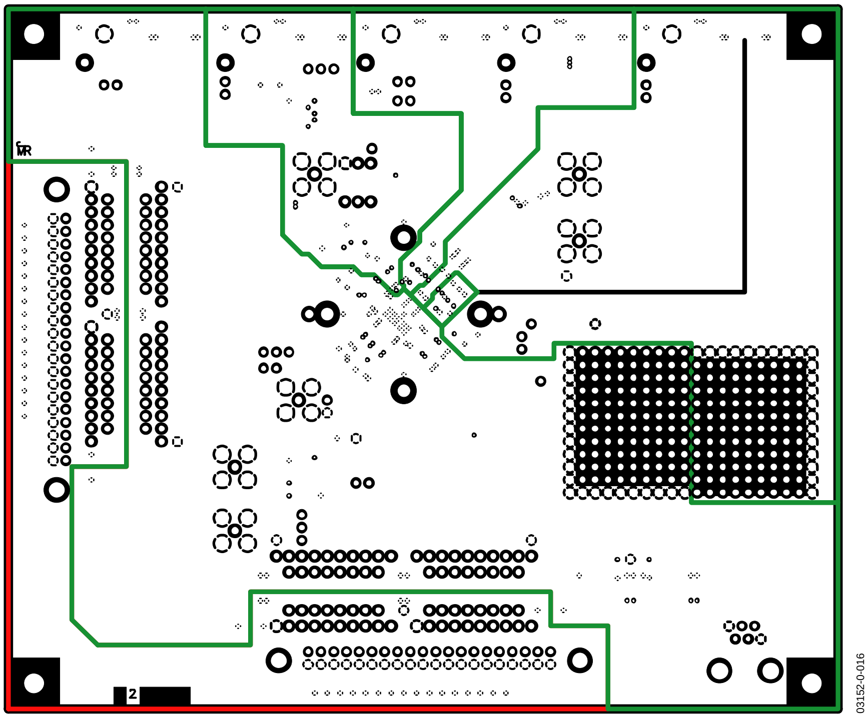


Figure 96. PCB Assembly, Layer 2 Metal (Ground Plane) Rev F Evaluation Board

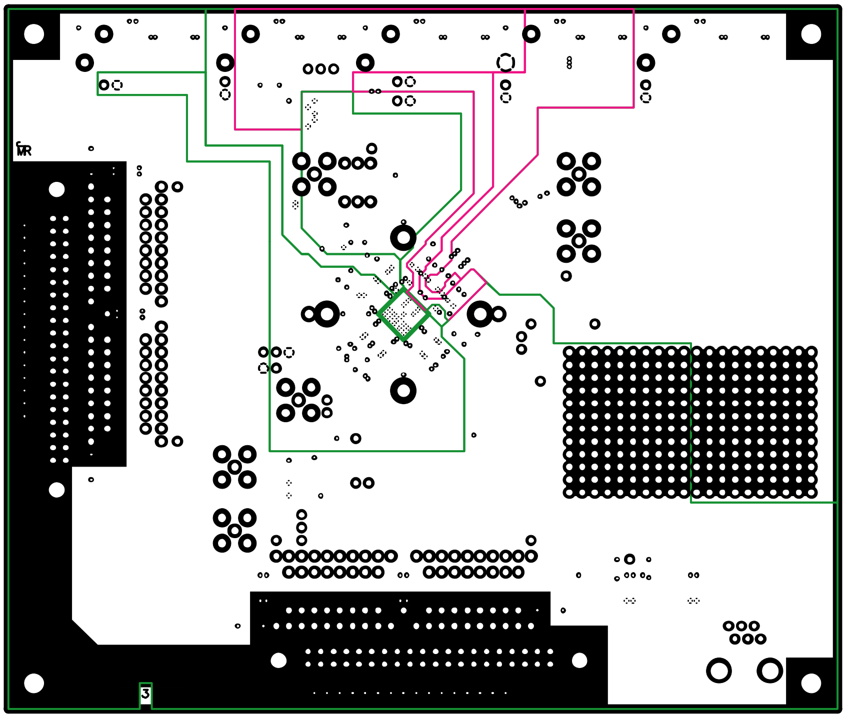


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Figure 97. PCB Assembly, Layer 3 Metal (Power Plane) Rev F Evaluation Board

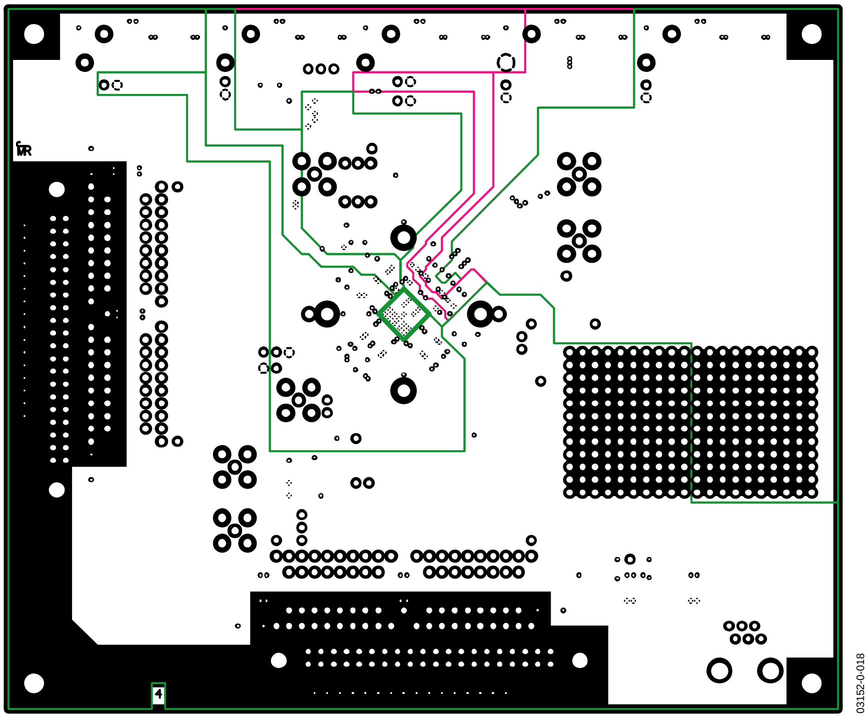

Figure 98. PCB Assembly, Layer 4 Metal (Power Plane) Rev F Evaluation Board

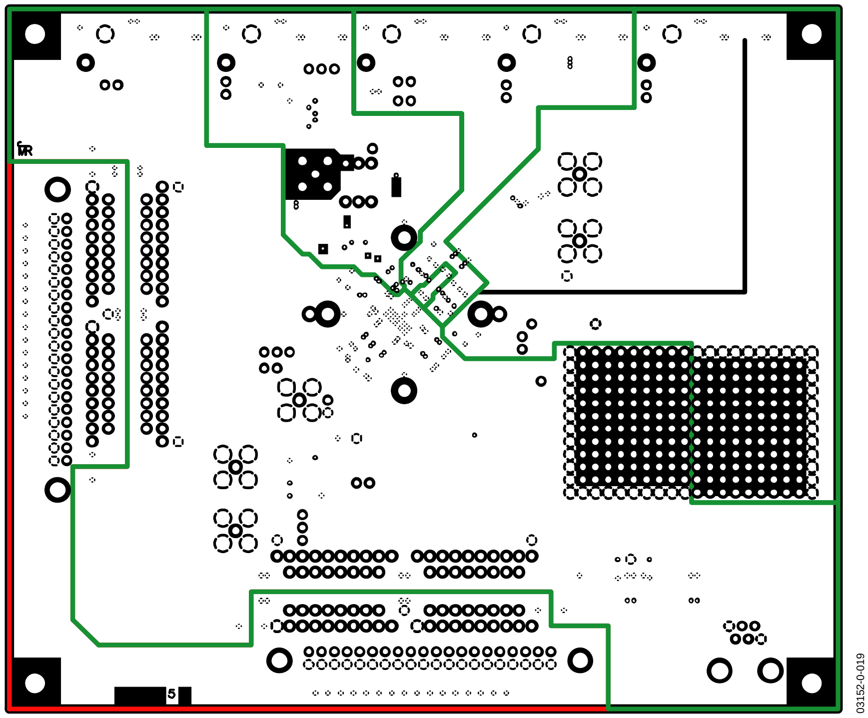

Figure 99. PCB Assembly, Layer 5 Metal (Ground Plane) Rev F Evaluation Board

OUTLINE DIMENSIONS

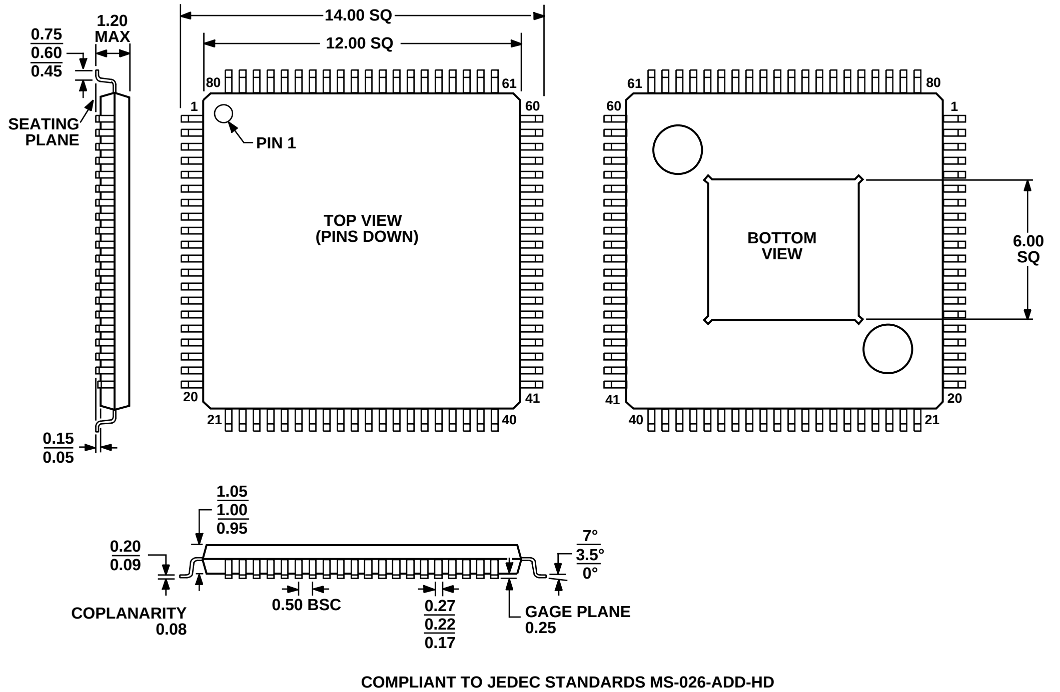

Figure 100. 80-Lead Thin Quad Flat Package, Exposed Pad [TQFP/EP]
(SV-80)
Dimensions shown in millimeters

ORDERING GUIDE

Model	Temperature Range	Package Description	Package Option
AD9786BSV	−40°C to +85°C	80-Lead TQFP	SV-80
AD9786BSVRL	−40°C to +85°C	80-Lead TQFP	SV-80
AD9786-EB		Evaluation Board	

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